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(54) **METHOD AND SYSTEM FOR PROGRAMMING, CALIBRATING AND DRIVING A LIGHT EMITTING DEVICE DISPLAY**

VERFAHREN UND SYSTEM ZUM PROGRAMMIEREN, KALIBRIEREN UND ANSTEUERN EINES LEUCHTBAUELEMENT-DISPLAY

PROCEDE ET SYSTEME DE PROGRAMMATION, DE CALIBRAGE ET DE COMMANDE D'UN AFFICHAGE A DISPOSITIF ELECTROLUMINESCENT

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Description

FIELD OF INVENTION

- 5 **[0001]** The present invention relates to display technologies, more specifically a method and system for programming, calibrating and driving a light emitting device display.

BACKGROUND OF THE INVENTION

- 10 **[0002]** Recently active-matrix organic light-emitting diode (AMOLED) displays with amorphous silicon (a-Si), poly-silicon, organic, or other driving backplane have become more attractive due to advantages over active matrix liquid crystal displays. For example, the advantages include: with a-Si besides its low temperature fabrication that broadens the use of different substrates and makes feasible flexible displays, its low cost fabrication, high resolution, and a wide viewing angle.
- 15 **[0003]** An AMOLED display includes an array of rows and columns of pixels, each having an organic light-emitting diode (OLED) and backplane electronics arranged in the array of rows and columns. Since the OLED is a current driven device, the pixel circuit of the AMOLED should be capable of providing an accurate and constant drive current.
- 20 **[0004]** U.S. patent No. 6,594, 606 discloses a method and system for calibrating passive pixels. U.S. patent No. 6,594, 606 measures data line voltage and uses the measurement for pre-charge. However, this technique does not provide the accuracy needed for active matrix, since the active matrix calibration should work for both backplane aging and OLED aging. Further, after pre-charge, current programming must be performed. Current-programming of current driven pixels is slow due to parasitic line capacitances and suffers from non-uniformity for large displays. The speed may be an issue when programming with small currents.
- 25 WO2005022498 discloses measuring a drive transistor threshold voltage and generating a compensation voltage. To measure the threshold voltage, WO2005022498 requires a sense line to be coupled to the pixel.
- US6738035 discloses measuring display characteristics of pixels and creating compensated video data. To measure the display characteristics of pixels, US6738035 requires a photo detector that measures the light intensities of the pixels. US6690344 discloses a signal processing circuit having a linear correction mechanism for making display properties linear with respect to the gradation level.
- 30 **[0005]** Other compensation techniques have been introduced. However, there is still a need to provide a method and system which is capable of providing constant brightness, achieving high accuracy and reducing the effect of the aging of the pixel circuit.

SUMMARY OF THE INVENTION

- 35 **[0006]** It is an object of the invention to provide a method and system that obviates or mitigates at least one of the disadvantages of existing systems.
- This object is achieved by the present invention as claimed in the independent claims. Advantageous and preferred embodiments of the present invention are defined by the dependent claims.
- 40 **[0007]** Other aspects and features of the present invention will be readily apparent to those skilled in the art from a review of the following detailed description of preferred embodiments in conjunction with the accompanying drawings.

BRIEF DESCRIPTION OF THE DRAWINGS

- 45 **[0008]** These and other features of the invention will become more apparent from the following description in which reference is made to the appended drawings wherein:
- [0009]** Figure 1 is a flow chart showing a process for calibration-scheduling in accordance with an embodiment of the present invention;
- 50 **[0010]** Figure 2 is a diagram showing an example of a system structure for implementing the calibration-scheduling of Figure 1;
- [0011]** Figure 3 is a diagram showing a system architecture for a voltage-extracting, programming and driving in accordance with an embodiment of the present invention;
- [0012]** Figure 4 is a diagram showing an example of the extracting, programming and driving system of Figure 3 and a pixel circuit;
- 55 **[0013]** Figure 5 is a diagram showing a further example of the extracting, programming and driving system of Figure 3 and a pixel circuit;
- [0014]** Figure 6 is a diagram showing a further example of the extracting, programming and driving system of Figure 3 and a pixel circuit;

[0015] Figure 7 is a diagram showing a further example of the extracting, programming and driving system of Figure 3 and a pixel circuit;

[0016] Figure 8 is a diagram showing a pixel circuit to which a step-calibration driving in accordance with an embodiment of the present invention is applied;

[0017] Figure 9 is a diagram showing an example of a driver and extraction block and the driving transistor of Figure 8;

[0018] Figure 10 is a diagram showing an example of an extraction algorithm implemented by a DPU block of Figure 9;

[0019] Figure 11 is a diagram showing a further example of the extraction algorithm implemented by the DPU block of Figure 9;

[0020] Figure 12 is a timing diagram showing an example of waveforms for the step-calibration driving;

[0021] Figure 13 is a timing diagram showing a further example of waveforms for the step-calibration driving;

[0022] Figure 14 is a diagram showing a pixel circuit to which the step-calibration driving is applicable;

[0023] Figure 15 is a graph showing the results of simulation for the step-calibration driving;

[0024] Figure 16 is a diagram showing an example of a system architecture for the step-calibration driving with a display array;

[0025] Figure 17 is a timing diagram showing an example of waveforms applied to the system architecture of Figure 16;

[0026] Figure 18 is a timing diagram showing an example of waveforms for a voltage/current extraction;

[0027] Figure 19 is a timing diagram showing a further example of waveforms for the voltage/current extraction;

[0028] Figure 20 is a diagram showing a pixel circuit to which the voltage/current extraction of Figure 19 is applicable;

[0029] Figure 21 is a timing diagram showing a further example of waveforms for the voltage/current extraction;

[0030] Figure 22 is a diagram showing a pixel circuit to which the voltage/current extraction of Figure 21 is applicable;

[0031] Figure 23 is a diagram showing a mirror based pixel circuit to which OLED removing in accordance with an embodiment of the present invention is applied;

[0032] Figure 24 is a diagram showing a programming path of Figure 23 when applying the OLED removing;

[0033] Figure 25 is a diagram showing an example of a system architecture for the OLED removing; and

[0034] Figure 26 is a graph showing the simulation result for the voltage on IDATA line for different threshold voltage.

DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS OF THE INVENTION

[0035] Embodiments of the present invention are described using a pixel including a light emitting device and a plurality of transistors. The light emitting device may be an organic light emitting diode (OLED). It is noted that "pixel" and "pixel circuit" may be used interchangeably.

[0036] Real-time calibration-scheduling for a display array having a plurality of pixels is described in detail. Figure 1 illustrates a process for a calibration-scheduling in accordance with an embodiment of the present invention. According to this technique, the pixels are calibrated based on their aging and/or usage during the normal operation of the display array.

[0037] A linked list of pixels is generated in step S2. The linked list contains an identification of a pixel with high brightness for calibration. The linked list is used to schedule the priority in calibration.

[0038] In step S4, " n " is chosen based on the display size and expected instability with time (e.g. shift in characteristics of transistors and light emitting device). " n " represents the number of pixels that are calibrated in each programming cycle. " n " may be one or more than one.

[0039] Then programming cycle starts at step S6. The step S6 includes steps S8-S16. The steps S8-S16 are implemented on a selected column of the display array.

[0040] In step S8, " n " pixels in the selected column are selected from the beginning of the linked list, hereinafter referred to as "Selected Pixels".

[0041] In step S10, "Calibration Mode" is enabled for the Selected Pixels, and "Normal Operation Mode" is enabled for the rest of the pixels in the selected column of the display array.

[0042] In step S12, all pixels in the selected column are programmed by a voltage source driver (e.g. 28 of Figure 2) which is connected to a data line of the pixel.

[0043] For the Selected Pixels, current flowing through the data line is monitored during the programming cycle. For the pixels other than the Selected Pixels in the selected column, the corresponding programming voltage is boosted using data stored in a memory (e.g. 34 of Figure 2), hereinafter referred to as " ΔV compensation memory".

[0044] In step S14, the monitored current is compared with the expected current that must flow through the data line. Then, a calibration data curve for the Selected Pixels is generated. The ΔV compensation memory is updated based on the calibration data curve.

[0045] The calibration data curve stored in the ΔV compensation memory for a pixel will be used to boost programming voltage for that pixel in the next programming cycles when that pixel is in the Normal Operation Mode.

[0046] In step S16, the identifications of the Selected Pixels are sent to the end of the linked list. The Selected Pixels have the lowest priority in the linked list for calibration.

[0047] During display operation (S6-S16), the linked list will provide a sorted priority list of pixels that must be calibrated. It is noted that in the description, the term "linked list" and the term "priority list" may be used interchangeably.

[0048] The operation goes back (S 18) to the step S8. The next programming cycle starts. A new column in the display array is activated (selected), and, new " n " pixels in the new activated column are selected from the top of the linked list.

[0049] The number of the Selected Pixels, " n ", is now described in detail. As described above, the number " n " is determined based on the display size and expected instability in device characteristics with time. It is assumed that the total number of pixels N is $N = 3 \times m_1 \times m_2$, where m_1 and m_2 are the number of rows and columns in the display, respectively.

[0050] The highest rate in characteristics shift is K ($=\Delta I/\Delta t.I$). Each programming cycle takes $t=1/f.m_2$. The maximum expected shift in characteristics after the entire display is calibrated is $\Delta I/I = K.t.N/n < e$, where e is the allowed error. After this the calibration can be redone from the beginning, and the error is eliminated. This shows that $n > K.t.N/e$ or $n > 3.K.m_1/f.e$. For instance, if $K = 1\%/hr$, $m_1 = 1024$, $f = 60$ Hz, and $e = 0.1\%$, then $n > 0.14$, which implies that it is needed to calibrate once in 5 programming cycles. This is achievable with one calibration unit, which operates only one time in 5 programming cycles. Each calibration unit enables calibration of one pixel at a programming cycle. If $e = 0.01\%$, $n > 1.4$. This means that two calibration units calibrating two pixels in each programming cycle are required. This shows that it is feasible to implement this calibration system with very low cost.

[0051] The frequency of calibration can be reduced automatically as the display ages, since shifts in characteristics will become slower as the time progresses. In addition, the pixels that are selected for calibration can be programmed with different currents depending on display data. The only condition is that their programming current is larger than a reference current. Therefore, the calibration can be performed at multiple brightness levels for one pixel to achieve higher accuracy.

[0052] The linked list is described in detail. In the linked list, the pixels with high brightness for calibration are listed. The display data is used to determine the pixels with high brightness for calibration. Calibration at low currents is slow and often not accurate. In addition, maximum shift in characteristics occurs for pixels with high current. Thus, in order to improve the accuracy and speed of calibration, the pixels, which must be programmed with currents higher than a threshold current I_{TH} , are selected and stored in the linked list.

[0053] I_{TH} is a variable and may be "0". For $I_{TH} = 0$, all pixels are listed in the linked list, and the calibration is performed for all pixels irrespective of their programming current.

[0054] The calibration-scheduling technique described above is applicable to any current programmed pixels, for example, but not limited to, a current mirror based pixel.

[0055] Figure 2 illustrates an example of a system structure for implementing the calibration-scheduling of Figure 1. A system 30 of Figure 2 for implementing calibration-scheduling algorithm is provided to a display array 10 having a plurality of pixel circuits 12. The pixel circuit 12 is a current programmed pixel circuit, such as, but not limited to a current mirror based pixel. The pixel circuits 12 are arranged in row and column.

[0056] The pixel circuit 12 may include an OLED and a plurality of transistors (e.g. TFTs). The transistor may be fabricated using amorphous silicon, nano/micro crystalline silicon, poly silicon, organic semiconductors technologies (e.g. organic TFT), NMOS/PMOS technology or CMOS technology (e.g. MOSFET). The display array 10 may be an AMOLED display array.

[0057] The pixel circuit 12 is operated by a gate line 14 connected to a gate driver 20, a data line 16 connected to a voltage data driver 28, and a power line connected to a power supply 24. In Figure 2, two data lines, two gate lines and two power lines are shown as an example. It is apparent that more than two data lines, two gate lines and two power lines may be provided to the display array 10.

[0058] The system 30 includes a calibration scheduler and memory block 32 for controlling programming and calibration of the display array 10, and a ΔV compensation memory 34 for storing ΔV compensation voltage (value). In each programming cycle, a column of the display array 10 is selected. The calibration scheduler and memory block 32 enables Normal Operation Mode or Calibration Mode for the selected column (i.e., data line) during that programming cycle.

[0059] The system 30 further includes a monitoring system for monitoring and measuring a pixel current. The monitoring system includes switches 36 and 38 and a voltage sensor 40 with an accurate resistor 42. In Figure 2, the switches 36 and 38 are provided for each data line as an example.

[0060] The system 30 further includes a generator for generating ΔV compensation voltage based on the monitoring result. The generator includes an analog/digital converter (A/D) 44, a comparator 46, and a translator 48. The A/D 44 converts the analog output of the voltage sensor 40 into a digital output. The comparator 46 compares the digital output to an output from the translator 48. The translator 48 implements function $f(V)$ on a digital data input 52. The translator 48 converts the current data input 52 to the voltage data input through $f(v)$. The result of the comparison by the comparator 46 is stored in the ΔV compensation memory 34.

[0061] The system 30 further includes an adder 50 for adding the digital data input 52 and the ΔV compensation voltage stored in the ΔV compensation memory 34. The voltage data driver 28 drives a data line based on the output of

the adder 50. The programming data for the data line is adjusted by adding the ΔV compensation voltage.

[0062] When the calibration scheduler and memory block 32 enables the Normal Operation Mode for a selected data line, the switch 36 is activated. The voltage output from the voltage data driver 28 is directly applied to the pixel on that data line.

[0063] When the calibration scheduler and memory block 32 enables the Calibration Mode for that data line, the switch 38 is activated. The voltage is applied to the pixel on that data line through the accurate resistor 42. The voltage drop across the resistor 42 at the final stages of the programming time (i.e. when initial transients are finished) is measured by the voltage sensor 40. The voltage drop monitored by the voltage sensor 40 is converted to digital data by the A/D 44. The resulting value of the voltage drop is proportional to the current flowing through the pixel if the pixel is a current programmed pixel circuit. This value is compared by the comparator 46 to the expected value obtained by the translator 48.

[0064] The difference between the expected value and the measured value is stored in the ΔV compensation memory 34, and will be used for a subsequent programming cycle. The difference will be used to adjust the data voltage for programming of that pixel in future.

[0065] The calibration scheduler and memory block 32 may include the linked list described above. In the beginning, the linked list is generated automatically. It may be just a list of pixels. However, during the operation it is modified.

[0066] The calibration of the pixel circuits with high brightness guarantees the high speed and accurate calibration that is needed in large or small area displays.

[0067] Since the display array 10 is driven using a voltage programming technique, it is fast and can be used for high-resolution and large area displays.

[0068] Due to speed, accuracy, and ease of implementation, the applications of the calibration-scheduling technique ranges from electroluminescent devices used for cellphones, personal organizers, monitors, TVs, to large area display boards.

[0069] The system 30 monitors and measures voltage drop which depends on time dependent parameters of the pixel, and generates a desirable programming data. However, the time dependent parameters of the pixel may be extracted by any mechanisms other than that of Figure 2.

[0070] A further technique for programming, extracting time dependent parameters of a pixel and driving the pixel is described in detail with reference to Figures 3-7. This technique includes voltage-extracting for calibration. Programming data is calibrated with the extracted information, resulting in a stable pixel current over time. Using this technique, the aging of the pixel is extracted.

[0071] Figure 3 illustrates a system architecture for implementing a voltage-extracting, programming and driving in accordance with an embodiment of the present invention. The system of Figure 3 implements the voltage-extracting and programming to a current mode pixel circuit 60. The pixel circuit 60 includes a light emitting device and a plurality of transistors having a driving transistor (not shown). The transistors may be TFTs.

[0072] The pixel circuit 60 is selected by a select line SEL and is driven by DATA on a data line 61. A voltage source 62 is provided to write a programming voltage V_P into the pixel circuit 60. A current-controlled voltage source (CCVS) 63 having a positive node and a negative node is provided to convert the current on the data line 61 to a voltage V_{ext} . A display controller and scheduler 64 operates the pixel circuit 60. The display controller and scheduler 64 monitors an extracted voltage V_{ext} output from the CCVS 63 and then controls the voltage source 62.

[0073] The resistance of CCVS 63 is negligible. Thus the current on the data line 61 is written as:

$$I_{Line} = I_{pixel} = \beta (V_P - V_T)^2 \quad \dots(1)$$

where I_{Line} represents the current on the data line 61, I_{pixel} represents a pixel current, V_T represents the threshold voltage of the driving transistor included in the pixel circuit 60, and β represents the gain parameter in the TFT characteristics.

[0074] As the threshold voltage of the driving TFT increases during the time, the current on the data line 61 decreases. By monitoring the extracted voltage V_{ext} , the display controller and scheduler 64 determines the amount of shift in the threshold voltage.

[0075] The threshold voltage V_T of the driving transistor can be calculate as:

$$V_T = V_P - (I_{Line}/\beta)^{0.5} \quad \dots(2)$$

[0076] The programming voltage V_P is modified with the extracted information. The extraction procedure can be implemented for one or several pixels during each frame time.

[0077] Figure 4 illustrates an example of a system for the voltage-extracting, programming and driving of Figure 3, which is employed with a top-emission current-cell pixel circuit 70. The pixel circuit 70 includes an OLED 71, a storage capacitor 72, a driving transistor 73 and switch transistors 74 and 75.

[0078] The transistors 73, 74 and 75 may be n-type TFTs. However, these transistors 73, 74 and 75 may be p-type transistors. The voltage-extracting and programming technique applied to the pixel circuit 70 is also applicable to a pixel circuit having p-type transistors.

[0079] The driving transistor 73 is connected to a data line 76 through the switch transistor 75, and is connected to the OLED 71, and also is connected to the storage capacitor 72 through the switch transistor 74. The gate terminal of the driving transistor 73 is connected to the storage capacitor 72. The gate terminals of the switch transistors 74 and 75 are connected to a select line SEL. The OLED 71 is connected to a voltage supply electrode or line VDD. The pixel circuit 70 is selected by the select line SEL and is driven by DATA on the data line 76.

[0080] A current conveyor (CC) 77 has X, Y and Z terminals, and is used to extract a current on the data line 76 without loading it. A voltage source 78 applies programming voltage to the Y terminal of the CC 77. In the CC 77, the X terminal is forced by feedback to have the same voltage as that of the Y terminal. Also, the current on the X terminal is duplicated into the Z terminal of the CC 77. A current-controlled voltage source (CCVS) 79 has a positive node and a negative node. The CCVS 79 converts the current on the Z terminal of the CC 77 into a voltage Vext.

[0081] Vext is provided to the display controller and scheduler 64 of Figure 3, where the threshold voltage of the driving transistor 73 is extracted. The display controller and scheduler 64 controls the voltage source 78 based on the extracted threshold voltage.

[0082] Figure 5 illustrates a further example of a system for the voltage-extracting, programming, and driving of Figure 3, which is employed with a bottom-emission current-cell pixel circuit 80. The pixel circuit 80 includes an OLED 81, a storage capacitor 82, a driving transistor 83, and switch transistors 84 and 85. The transistors 83, 84 and 85 may be n-type TFTs. However, these transistors 83, 84 and 85 may be p-type transistors.

[0083] The driving transistor 83 is connected to a data line 86 through the switch transistor 85, and is connected to the OLED 81, and also is connected to the storage capacitor 82. The gate terminal of the driving transistor 83 is connected to a voltage supply line VDD through the switch transistor 84. The gate terminals of the switch transistors 84 and 85 are connected to a select line SEL. The pixel circuit 80 is selected by the select line SEL and is driven by DATA on the data line 86.

[0084] A current conveyor (CC) 87 has X, Y and Z terminals, and is used to extract a current on the data line 86 without loading it. A voltage source 88 applies a negative programming voltage at the Y terminal of the CC 87. In the CC 87, the X terminal is forced by feedback to have the same voltage as that of the Y terminal. Also, the current on the X terminal is duplicated into the Z terminal of the CC 87. A current-controlled voltage source (CCVS) 89 has a positive node and a negative node. The CCVS 89 converts the current of the Z terminal of the CC 87 into a voltage Vext.

[0085] Vext is provided to the display controller and scheduler 64 of Figure 3, where the threshold voltage of the driving transistor 83 is extracted. The display controller and scheduler 64 controls the voltage source 88 based on the extracted threshold voltage.

[0086] Figure 6 illustrates a further example of a system for the voltage-extracting, programming and driving of Figure 3, which is employed with a top-emission current-mirror pixel circuit 90. The pixel circuit 90 includes an OLED 91, a storage capacitor 92, mirror transistors 93 and 94, and switch transistors 95 and 96. The transistors 93, 94, 95 and 96 may be n-type TFTs. However, these transistors 93, 94, 95 and 96 may be p-type transistors.

[0087] The mirror transistor 93 is connected to a data line 97 through the switch transistor 95, and is connected to the storage capacitor 92 through the switch transistor 96. The gate terminals of the mirror transistors 93 and 94 are connected to the storage capacitor 92 and the switch transistor 96. The mirror transistor 94 is connected to a voltage supply electrode or line VDD through the OLED 91. The gate terminals of the switch transistors 95 and 96 are connected to a select line SEL. The pixel circuit 90 is selected by the select line SEL and is driven by DATA on the data line 97.

[0088] A current conveyor (CC) 98 has X, Y and Z terminals, and is used to extract the current of the data line 97 without loading it. A voltage source 99 applies a positive programming voltage at the Y terminal of the CC 98. In the CC 98, the X terminal is forced by feedback to have the same voltage as the voltage of the Y terminal. Also, the current on the X terminal is duplicated into the Z terminal of the CC 98. A current-controlled voltage source (CCVS) 100 has a positive node and a negative node. The CCVS 100 converts a current on the Z terminal of the CC 98 into a voltage Vext.

[0089] Vext is provided to the display controller and scheduler 64 of Figure 3, where the threshold voltage of the driving transistor 93 is extracted. The display controller and scheduler 64 controls the voltage source 99 based on the extracted threshold voltage.

[0090] Figure 7 illustrates a further example of a system for the voltage-extracting, programming and driving of Figure 3, which is employed with a bottom-emission current-mirror pixel circuit 110. The pixel circuit 110 includes an OLED 111, a storage capacitor 112, mirror transistors 113 and 116, and switch transistors 114 and 115. The transistors 113,

114, 115 and 116 may be n-type TFTs. However, these transistors 113, 114, 115 and 116 may be p-type transistors.

[0091] The mirror transistor 113 is connected to a data line 117 through the switch transistor 114, and is connected to the storage capacitor 112 through the switch transistor 115. The gate terminals of the mirror transistors 113 and 116 are connected to the storage capacitor 112 and the switch transistor 115. The mirror transistor 116 is connected to a voltage supply line VDD. The mirror transistors 113, 116 and the storage capacitor 112 are connected to the OLED 111. The gate terminals of the switch transistors 114 and 115 are connected to a select line SEL. The pixel circuit 110 is selected by the select line SEL and is driven by DATA on the data line 117.

[0092] A current conveyor (CC) 118 has X, Y and Z terminals, and is used to extract the current of the data line 117 without loading it. A voltage source 119 applies a positive programming voltage at the Y terminal of the CC 118. In the CC 118, the X terminal is forced by feedback to have the same voltage as the voltage of the Y terminal of the CC 118. Also, the current on the X terminal is duplicated into the Z terminal of the CC 118. A current-controlled voltage source (CCVS) 120 has a positive node and a negative node. The 120 converts the current on the Z terminal of the CC 118 into a voltage Vext.

[0093] Vext is provided to the display controller and scheduler 64 of Figure 3, where the threshold voltage of the driving transistor 113 is extracted. The display controller and scheduler 64 controls the voltage source 119 based on the extracted threshold voltage.

[0094] Referring to Figures 3-7, using the voltage-extracting technique, time dependent parameters of a pixel (e.g. threshold shift) can be extracted. Thus, the programming voltage can be calibrated with the extracted information, resulting in a stable pixel current over time. Since the voltage of the OLED (i.e. 71 of Figure 4, 81 of Figure 5, 91 of Figure 6, 111 of Figure 7) affects the current directly, the voltage-extracting driving technique described above can also be used to extract OLED degradation as well as the threshold shift.

[0095] The voltage-extracting technique described above can be used with any current-mode pixel circuit, including current-mirror and current-cell pixel circuit architectures, and are applicable to the display array 10 of Figure 2. A stable current independent of pixel aging under prolonged display operation can be provided using the extracted information. Thus, the display operating lifetime is efficiently improved.

[0096] It is noted that the transistors in the pixel circuits of Figures 3-7 may be fabricated using amorphous silicon, nano/micro crystalline silicon, poly silicon, organic semiconductors technologies (e.g. organic TFT), NMOS/PMOS technology or CMOS technology (e.g. MOSFET). The pixel circuits of Figures 3-7 may form AMOLED display arrays.

[0097] A further technique for programming, extracting time dependent parameters of a pixel and driving the pixel is described in detail with reference to Figures 8-17. The technique includes a step-calibration driving technique. In the step-calibration driving technique, information on the aging of a pixel (e.g. threshold shift) is extracted. The extracted information will be used to generate a stable pixel current/luminance. Despite using the one-bit extraction technique, the resolution of the extracted aging is defined by display drivers. Also, the dynamic effects are compensated since the pixel aging is extracted under operating condition, which is similar to the driving cycle.

[0098] Figure 8 illustrates a pixel circuit 160 to which a step-calibration driving in accordance with an embodiment of the present invention is applied. The pixel circuit 160 includes an OLED 161, a storage capacitor 162, and a driving transistor 163 and switch transistors 164 and 165. The pixel circuit 160 is a current-programmed, 3-TFT pixel circuit. A plurality of the pixel circuits 160 may form an AMOLED display.

[0099] The transistors 163, 164 and 165 are n-type TFTs. However, the transistors 163, 164 and 165 may be p-type TFTs. The step-calibration driving technique applied to the pixel circuit 160 is also applicable to a pixel circuit having p-type transistors. The transistors 163, 164 and 165 may be fabricated using amorphous silicon, nano/micro crystalline silicon, poly silicon, organic semiconductors technologies (e.g. organic TFT), NMOS/PMOS technology or CMOS technology (e.g. MOSFET).

[0100] The gate terminal of the driving transistor 163 is connected to a signal line VDATA through the switch transistor 164, and also connected to the storage capacitor 162. The source terminal of the driving transistor 163 is connected to a common ground. The drain terminal of the driving transistor 163 is connected to a monitor line MONITOR through the switch transistor 165, and also is connected to the cathode electrode of the OLED 161.

[0101] The gate terminal of the switch transistor 164 is connected to a select line SEL1. The source terminal of the switch transistor 164 is connected to the gate terminal of the driving transistor 163, and is connected to the storage capacitor 162. The drain terminal of the switch transistor 164 is connected to VDATA.

[0102] The gate terminal of the switch transistor 165 is connected to a select line SEL2. The source terminal of the switch transistor 165 is connected to MONITOR. The drain terminal of the switch transistor 165 is connected to the drain terminal of the driving transistor 163 and the cathode electrode of the OLED 161. The anode electrode of the OLED 161 is connected to a voltage supply electrode or line VDD.

[0103] The transistors 163 and 164 and the storage capacitor 162 are connected at node A3. The transistors 163 and 165 and the OLED 161 are connected at node B3.

[0104] Figure 9 illustrates an example of a driver and extraction block 170 along with the driving transistor 163 of Figure 8. In Figure 9, each of Rs 171a and Rs 171b represents the ON resistance of the switch transistors (e.g. 164,

165 of Figure 8). C_s represents the storage capacitor of the pixel, C_{OLED} represents the OLED capacitance, and C_P represents the line parasitic capacitance. In Figure 9, the OLED is presented as a capacitance.

[0105] A block 173 is used to extract the threshold voltage of the driving transistor, during the extraction cycle. The block 173 may be a current sense amplifier (SA) or a current comparator. In the description, the block 173 is referred to as "SA block 173".

[0106] If the current of the MONITOR line is higher than a reference current (IREF), the output of the SA block 173 (i.e. Triggers of Figure 10, 11) becomes one. If the current of the MONITOR line is less than the reference current (IREF), the output of the SA block 173 becomes zero.

[0107] It is noted that the SA block 173 can be shared between few columns result in less overhead. Also, the calibration of the pixel circuit can be done one at a time, so the extraction circuits can be shared between the all columns.

[0108] A data process unit (DPU) block 172 is provided to control the programming cycle, contrast, and brightness, to perform the calibration procedure and to control the driving cycle. The DPU block 172 implements extraction algorithm to extract (estimate) the threshold voltage of the driving transistor based on the output from the SA block 173, and controls a driver 174 which is connected to the driving transistor 163.

[0109] Figure 10 illustrates an example of the extraction algorithm implemented by the DPU block 172 of Figure 9. The algorithm of Figure 10 is in a part of the DPU block 172. In Figure 10, $V_T(i, j)$ represents the extracted threshold voltage for the pixel (i, j) at the previous extraction cycle, V_S represents the resolution of the driver 174, "i" represents a row of a pixel array and "j" represents a column of a pixel array. Trigger conveys the comparison results of the SA block 173 of Figure 9. Less_state 180 determines the situation in which the actual V_T of the pixel is less than the predicted $V_T(V_{TM})$, Equal_state 181 determines the situation in which the predicted $V_T(V_{TM})$ and the actual V_T of the pixel are equal, and Great_state 182 determines the situation in which the actual V_T of the pixel is greater than the predicted $V_T(V_{TM})$.

[0110] The DPU block 172 of Figure 9 determines an intermediate threshold voltage V_{TM} as follows:

(A1) When $s(i, j) = \text{Less_state}$ (180), the actual threshold voltage is less than $V_T(i, j)$, V_{TM} is set to $(V_T(i, j) - V_S)$.

(A2) When $s(i, j) = \text{Equal_state}$ (181), the actual threshold voltage is equal to $V_T(i, j)$, V_{TM} is set to $V_T(i, j)$.

(A3) When $s(i, j) = \text{Greater_state}$ (182), the actual threshold voltage is greater than $V_T(i, j)$, V_{TM} is set to $(V_T(i, j) + V_S)$.

where $s(i, j)$ represents the previous state of the pixel (i, j) stored in a calibration memory (e.g. 208 of Figure 16).

[0111] Figure 11 illustrates a further example of the extraction algorithm implemented by the DPU block 172 of Figure 9. The algorithm of Figure 11 is in a part of the DPU block 172 of Figure 9. In Figure 11, $V_T(i, j)$ represents the extracted threshold voltage for the pixel (i, j) at the previous extraction cycle, V_S represents the resolution of the driver 174, "i" represents a row of a pixel array and "j" represents a column of a pixel array. Trigger conveys the comparison results of the SA block 173.

[0112] Further, in Figure 11, V_{res} represents the step that will be added/subtracted to the predicted $V_T(V_{TM})$ in order achieve the actual V_T of the pixel, A represents the reduction gain of a prediction step, and K represents the increase gain of the prediction step.

[0113] The operation of Figure 11 is the same as that of Figure 10, except that it has gain extra states L2 and G2 for rapid extraction of abrupt changes. In the gain states, the step size is increased to follow the changes more rapidly. L1 and G1 are the transition states which define the V_T change is abrupt or normal.

[0114] Figure 12 illustrates an example of waveforms applied to the pixel circuit 160 of Figure 8. In Figure 12, $V_{Call} = V_B + V_{TM}$, and $V_{DR} = V_P + V_T(i, j) + V_{REF}$, where V_B represents the bias voltage during the extraction cycle, V_{TM} is defined based on the algorithm shown in Figure 10 or 11, V_P represents a programming voltage, $V_T(i, j)$ represents the extracted threshold voltage at the previous extraction cycle, V_{REF} represents the source voltage of the driving transistor during the programming cycle.

[0115] Referring to Figures 8-12, the operation of the pixel circuit 160 includes operating cycles X51, X52, X53, and X54. In Figure 12, an extraction cycle is separated from a programming cycle. The extraction cycle includes X51 and X52, and the programming cycle includes X53. X54 is a driving cycle. At the end of the programming cycle, node A3 is charged to $(V_P + V_T)$ where V_P is a programming voltage and V_T is the threshold voltage of the driving transistor 163.

[0116] In the first operating cycle X51: SEL1 and SEL 2 are high. Node A3 is charged to V_{cal} , and node B3 is charged to V_{REF} . V_{cal} is $V_B + V_{TM}$ in which V_B is a bias voltage, and V_{TM} the predicted V_T , and V_{REF} should be larger than $V_{DD} - V_{OLED0}$ where V_{OLED0} is the ON voltage of the OLED 161.

[0117] In the second operating cycle X52: SEL1 goes to zero. The gate-source voltage of the driving transistor 163 is given by:

$$V_{GS}=V_B+V_{TM}+\Delta V_B+\Delta V_{TM}-\Delta V_{T2}-\Delta V_H$$

where V_{GS} represents the gate-source voltage of the driving transistor 163, ΔV_B , ΔV_{TM} , ΔV_{T2} and ΔV_H are the dynamic effects depending on V_B , V_{TM} , V_{T2} and V_H , respectively. V_{T2} represents the threshold voltage of the switch transistor 164, and V_H represents the change in the voltage of SEL1 at the beginning of second operating cycle X52 when it goes to zero.

[0118] The SA block 173 is tuned to sense the current larger than $\beta(V_B)^2$, so that the gate-source voltage of the driving transistor 163 is larger than $(V_B + V_T)$, where β is the gain parameter in the I-V characteristic of the driving transistor 163.

[0119] As a result, after few iterations, V_{TM} and the extracted threshold voltage $V_T(i, j)$ for the pixel (i, j) converge to:

$$V_{TM}=V_T-\gamma \cdot (V_B+V_T+V_{T2}-V_H)$$

$$\gamma = \frac{C_{g2} / (2 \cdot C_s)}{1 + C_{g2} / (2 \cdot C_s)}$$

where C_{g2} represents the gate capacitance of the switch transistor 164.

[0120] In the third operating cycle X53: SEL1 is high. VDATA goes to V_{DR} . Node A3 is charged to $[V_P + V_T(i, j) - \gamma(V_P - V_B)]$.

[0121] In the fourth operating cycle X54: SEL1 and SEL2 go to zero. Considering the dynamic effects, the gate-source voltage of the driving transistor 163 can be written as:

$$V_{GS}=V_P+V_T$$

[0122] Therefore, the pixel current becomes independent of the static and dynamic effects of the threshold voltage shift.

[0123] In Figure 12, the extraction cycle and the programming cycle are shown as separated cycles. However, the extraction cycle and the programming cycle may be merged as shown in Figure 13. Figure 13 illustrates a further example of waveforms applied to the pixel circuit 160 of Figure 8.

[0124] Referring to Figures 8-11 and 13, the operation of the pixel circuit 160 includes operating cycles X61, X62 and X63. Programming and extraction cycles are merged into the operating cycles X61 and X62. The operating cycle X63 is a driving cycle.

[0125] During the programming cycle, the pixel current is compared with the desired current, and the threshold voltage of the driving transistor is extracted with the algorithm of Figure 10 or 11. The pixel circuit 160 is programmed with $V_{DR}=V_P+V_T(i, j)+V_{REF}$ during the operating cycle X61. Then the pixel current is monitored through the MONITOR line, and is compared with the desired current. Based on the comparison result and using the extraction algorithm of Figures 10 or 11, the threshold voltage $V_T(i, j)$ is updated.

[0126] In Figure 8, two select lines SEL1 and SEL2 are shown. However, a signal select line (e.g. SEL1) can be used as a common select line to operate the switch transistors 164 and 165. When using the common select line, SEL1 of Figure 12 stays at high in the second operating cycle X52, and the VGS remains at (V_B+V_{TM}) . Therefore, the dynamic effects are not detected.

[0127] The step-calibration driving technique described above is applicable to the pixel circuit 190 of Figure 14. The pixel circuit 190 includes an OLED 191, a storage capacitor 192, and a driving transistor 193 and switch transistors 194 and 195. The pixel circuit 190 is a current-programmed, 3-TFT pixel circuit. A plurality of the pixel circuits 190 may form an AMOLED display.

[0128] The transistors 193, 194 and 195 are n-type TFTs. However, the transistors 193, 194 and 195 may be p-type TFTs. The step-calibration driving technique applied to the pixel circuit 190 is also applicable to a pixel circuit having p-type transistors. The transistors 193, 194 and 195 may be fabricated using amorphous silicon, nano/micro crystalline silicon, poly silicon, organic semiconductors technologies (e.g. organic TFT), NMOS/PMOS technology or CMOS technology (e.g. MOSFET).

[0129] The gate terminal of the driving transistor 193 is connected to a signal line VDATA through the switch transistor 194, and also connected to the storage capacitor 192. The source terminal of the driving transistor 193 is connected to

the anode electrode of the OLED 191, and is connected to a monitor line MONITOR through the switch transistor 195. The drain terminal of the driving transistor 193 is connected to a voltage supply line VDD. The gate terminals of the transistors 194 and 195 are connected to select lines SEL1 and SEL2, respectively.

[0130] The transistors 193 and 194 and the storage capacitor 192 are connected at node A4. The transistor 195, the OLED 191 and the storage capacitor 192 are connected at node B4.

[0131] The structure of the pixel circuit 190 is similar to that of Figure 8, except that the OLED 191 is at the source terminal of the driving transistor 193. The operation of the pixel circuit 190 is the same as that of Figure 12 or 13.

[0132] Since the source terminal of the drive TFT 193 is forced to VREF during the extraction cycle (X51 and X52 or X62), the extracted data is independent of the ground bouncing. Also, during the programming cycle (X53 or X61), the source terminal of the drive TFT is forced to VREF, the gate-source voltage of the drive TFT becomes independent of the ground bouncing. As a result of these conditions, the pixel current is independent of ground bouncing.

[0133] Figure 15 illustrates the results of simulation for the step-calibration driving technique. In Figure 15, "Case I" represents an operation of Figure 8 where SEL1 goes to zero in the second operating cycle (X52 of Figure 12); "Case II" represents an operation of Figure 8 where SEL1 stays at high in the second operating cycle.

[0134] In Figure 15, ΔV_{TR} is the minimum detectable shift in the threshold voltage of the driving transistor (e.g. 163 of Figure 8), ΔV_{T2R} is the minimum detectable shift in the threshold voltage of the switch transistor (e.g. 164 of Figure 8), and I_{PL} is the pixel current of the pixel during the driving cycle.

[0135] The pixel current of Case II is smaller than that of Case I for a given programming voltage due to the dynamic effects of the threshold voltage shift. Also, the pixel current of Case II increases as the threshold voltage of the driving transistor increases (a), and decreases as the threshold voltage of the switch transistor decreases (b). However, the pixel current of Case I is stable. The maximum error induced in the pixel current is less than %0.5 for any shift in the threshold voltage of the driving and switch TFTs. It is obvious that ΔV_{T2R} is larger than ΔV_{TR} because the effect of a shift in V_T on the pixel current is dominant. These two parameters are controlled by the resolution (V_S) of the driver (e.g. 174 of Figure 9), and the SNR of the SA block (e.g. 193 of Figure 9). Since a shift smaller than ΔV_{TR} cannot be detected, and also the time constant of threshold-shift is large, the extraction cycles (e.g. X51, X52 of Figure 12) can be done after a long time interval consisting of several frames, leading to lower power consumption. Also, the major operating cycles become the other programming cycle (e.g. X53 of Figure 12) and the driving cycle (e.g. X54 of Figure 12). As a result, the programming time reduces significantly, providing for high-resolution, large-area AMOLED displays where a high-speed programming is prerequisite.

[0136] Figure 16 illustrates an example of a system architecture for the step-calibration driving with a display array 200. The display array 200 includes a plurality of the pixel circuits (e.g. 160 of Figure 8 or 190 of Figure 14).

[0137] A gate driver 202 for selecting the pixel circuits, a drivers/SAs block 204, and a data process and calibration unit block 206 are provided to the display array 200. The drivers/SAs block 204 includes the driver 174 and the SA block 173 of Figure 9. The data process and calibration unit block 206 includes the DPU block 172 of Figure 9. "Calibration" in Figure 16 includes the calibration data from a calibration memory 208, and may include some user defined constants for setting up calibration data processing. The contrast and the brightness inputs are used to adjust the contrast and the brightness of the panel by the user. Also, gamma-correction data is defined based on the OLED characteristic and human eye. The gamma-correction input is used to adjust the pixel luminance for human eyes.

[0138] The calibration memory 208 stores the extracted threshold voltage $V_T(i, j)$ and the state $s(i, j)$ of each pixel. A memory 210 stores the other required data for the normal operation of a display including gamma correction, resolution, contrast, and etc. The DPU block performs the normal tasks assigned to a controller and scheduler in a display. Besides, the algorithm of Figure 10 or 11 is added to it to perform the calibration.

[0139] Figure 17 illustrates an example of waveforms applied to the system architecture of Figure 16. In Figure 17, each of ROW[1], ROW[2], and ROW[3] represents a row of the display array 200, "E" represents an extraction operation, "P" represents a programming operation and "D" represents a driving operation. It is noted that the extraction cycles (E) are not required to be done for all the frame cycle. Therefore, after a long time interval (extraction interval), the extraction is repeated for a pixel.

[0140] As shown in Figure 17, only one extraction procedure occurs during a frame time. Also, the VT extraction of the pixel circuits at the same row is preformed at the same time.

[0141] Therefore, the maximum time required to refresh a frame is:

$$\tau_F = n \cdot \tau_P + \tau_E$$

where τ_F represents the frame time, τ_P represents the time required to write the pixel data into the storage capacitor (e.g. 162 of Figure 8), τ_E represents the extraction time, and n represents the number of row in the display array (e.g. 200 of Figure 16).

[0142] Assuming $\tau_E = m \cdot \tau_P$, the frame time τ_F can be written as:

$$\tau_F = (n + m) \cdot \tau_P$$

where m represents the timing required for the extraction cycles in the scale of programming cycle timing (τ_P).

[0143] For example, for a Quarter Video Graphics Array (QVGA) display (240x320) with frame rate of 60Hz, if $m=10$, the programming time of each row is 66 μ s, and the extraction time is 0.66ms.

[0144] It is noted that the step-calibration driving technique described above is applicable to any current-programmed pixel circuit other than those of Figures 8 and 14.

[0145] Using the step-calibration driving technique, the time dependent parameter(s) of a pixel, such as threshold shift, is extracted. Then, the programming-voltage is calibrated with the extracted information, resulting in a stable pixel current over time. Further, a stable current independent of the pixel aging under prolonged display operation can be provided to the pixel circuit, which efficiently improves the display operating lifetime.

[0146] A technique for programming, extracting time dependent parameters of a pixel and driving the pixel in accordance with a further embodiment of the present invention is described in detail. The technique includes extracting information on the aging of a pixel (e.g. OLED luminance) by monitoring OLED voltage or OLED current, and generating luminance. The programming voltage is calibrated with the extracted information, resulting in stable brightness over time.

[0147] Since the OLED voltage/current has been reported to be correlated with the brightness degradation in the OLED (e.g. 161 of Figure 8, 191 of Figure 14), the programming voltage can be modified by the OLED voltage/current to provide a constant brightness.

[0148] For example, during the driving cycle, the voltage/current of the OLED (161 of Figure 8 or 191 of Figure 14) is extracted while SEL2 is high. Since the OLED voltage or current has been reported to be correlated with the brightness degradation in the OLED, the programming voltage can be modified by the OLED voltage to provide a constant brightness.

[0149] Figure 18 illustrates an example of waveforms for the voltage/current extraction. The waveforms of Figure 18 are applicable to the pixel circuit 160 of Figure 8 and the pixel circuit 190 of Figure 14 to extract OLED voltage/current. The operation of Figure 18 includes operating cycles X71, X72 and X73. The operating cycles X71 and X72 are an OLED extraction cycle. The operating cycle X73 is one of the operating cycles shown in Figure 12 and 13.

[0150] During the first operating cycle X71, SEL1 and SEL2 are high, and VDATA is zero. The gate-source voltage of the driving transistor (e.g. 163 of Figure 8) becomes zero. A current or voltage is applied to the OLED (161 of Figure 8) through the MONITOR line.

[0151] During the second operating cycle X72, SEL2 is high and SEL1 is low. The OLED voltage or current is extracted through the MONITOR line using the algorithm presented in Figures 10 or 11. This waveform can be combined with any other driving waveform.

[0152] In the above description, the algorithm of Figure 10 and 11 is used to predict the aging data, i.e. V_T shift, based on the comparison results (current with current or voltage with voltage). However, the algorithm of Figures 10 and 11 is applicable to predict the shift in the OLED voltage V_{OLED} by replacing V_T with the V_{OLED} and the comparison result of OLED current/voltage with a reference current/voltage. In the description above, the system architecture shown in Figure 9 is used to compensate for the threshold shift. However, it is understood that the OLED data is also extracted when the architecture of Figure 9, i.e. DPU 172, block 173, driver 174, is used. This data can be used to compensate for the OLED shift.

[0153] The operating cycle X73 can be any operating cycle including the programming cycle. This depends on the status of the panel after OLED extraction. If it is during the operation, then X73 is the programming cycle of the waveforms in Figures 12 and 13. The OLED voltage can be extracted during the driving cycle X55/X63 of Figure 12/13. During the driving cycle X55/X63, the SEL2 of Figure 8 or 14 goes to a high voltage, and so the voltage of the OLED can be read back through the MONITOR for a specific pixel current.

[0154] Figure 19 illustrates a further example of waveforms for the voltage/current extraction. Figure 20 illustrates a pixel circuit 220 to which the voltage/current extraction of Figure 19 is applied.

[0155] Referring to Figure 20, the pixel circuit 220 includes an OLED 221, a storage capacitor 222, and a driving transistor 223 and switch transistors 224 and 225. A plurality of the pixel circuits 220 may form an AMOLED display.

[0156] The transistors 223, 224 and 225 are n-type TFTs. However, the transistors 223, 224 and 225 may be p-type TFTs. The voltage/current extraction technique applied to the pixel circuit 220 is also applicable to a pixel circuit having p-type transistors. The transistors 223, 224 and 225 may be fabricated using amorphous silicon, nano/micro crystalline silicon, poly silicon, organic semiconductors technologies (e.g. organic TFT), NMOS/PMOS technology or CMOS technology (e.g. MOSFET).

[0157] The gate terminal of the driving transistor 223 is connected to the source terminal of the switch transistor 224,

and also connected to the storage capacitor 222. The one terminal of the driving transistor 223 is connected to a common ground. The other terminal of the driving transistor 223 is connected to a monitor and data line MONITOR/DATA through the switch transistor 235, and is also connected to the cathode electrode of the OLED 221.

[0158] The gate terminal of the switch transistor 224 is connected to a select line SEL1. The one terminal of the switch transistor 224 is connected to the gate terminal of the driving transistor 223, and is connected to the storage capacitor 222. The other terminal of the switch transistor 224 is connected to the cathode electrode of the OLED 221.

[0159] The gate terminal of the switch transistor 225 is connected to a select line SEL2. The one terminal of the switch transistor 225 is connected to MONITOR/DATA. The other terminal of the switch transistor 225 is connected to the driving transistor 223 and the cathode electrode of the OLED 221. The anode electrode of the OLED 221 is connected to a voltage supply electrode or line VDD.

[0160] The transistors 223 and 224 and the storage capacitor 222 are connected at node A5. The transistors 223 and 225 and the OLED 221 are connected at node B5.

[0161] The pixel circuit 220 is similar to the pixel circuit 160 of Figure 8. However, in the pixel circuit 220, the MONITOR/DATA line is used for monitoring and programming purpose.

[0162] Referring to Figures 19-20, the operation of the pixel circuit 220 includes operating cycles X81, X82 and X83.

[0163] During the first operating cycle X81, SEL1 and SEL2 are high and MONITOR/DATA is zero. The gate-source voltage of the driving transistor (223 of Figure 20) becomes zero.

[0164] During the second operating cycle X82, a current or voltage is applied to the OLED through the MONITOR/DATA line, and its voltage or current is extracted. As described above, the shift in the OLED voltage is extracted using the algorithm presented in Figure 10 or 11 based on the monitored voltage or current. This waveform can be combined with any driving waveform.

[0165] The operating cycle X83 can be any operating cycle including the programming cycle. This depends on the status of the panel after OLED extraction..

[0166] The OLED voltage/current can be extracted during the driving cycle of the pixel circuit 220 of Figure 20 after it is programmed for a constant current using any driving technique. During the driving cycle the SEL2 goes to a high voltage, and so the voltage of the OLED can be read back through the MONITOR/DATA line for a specific pixel current.

[0167] Figure 21 illustrates a further example of waveforms for the voltage/current extraction technique. Figure 22 illustrates a pixel circuit 230 to which the voltage/current extraction of Figure 21 is applied. The waveforms of Figure 21 is also applicable to the pixel circuit 160 of Figure 8 to extract OLED voltage/current.

[0168] Referring to Figure 22, the pixel circuit 230 includes an OLED 231, a storage capacitor 232, and a driving transistor 233 and switch transistors 234 and 235. A plurality of the pixel circuits 230 may form an AMOLED display.

[0169] The transistors 233, 234 and 235 are n-type TFTs. However, the transistors 233, 234 and 235 may be p-type TFTs. The voltage/current extraction technique applied to the pixel circuit 230 is also applicable to a pixel circuit having p-type transistors. The transistors 233, 234 and 235 maybe fabricated using amorphous silicon, nano/micro crystalline silicon, poly silicon, organic semiconductors technologies (e.g. organic TFT), NMOS/PMOS technology or CMOS technology (e.g. MOSFET).

[0170] The gate terminal of the driving transistor 233 is connected to the source terminal of the switch transistor 234, and also connected to the storage capacitor 232. The one terminal of the driving transistor 233 is connected to a voltage supply line VDD. The other terminal of the driving transistor 233 is connected to a monitor and data line MONITOR/DATA through the switch transistor 235, and is also connected to the anode electrode of the OLED 231.

[0171] The gate terminal of the switch transistor 234 is connected to a select line SEL1. The one terminal of the switch transistor 234 is connected to the gate terminal of the driving transistor 233, and is connected to the storage capacitor 232. The other terminal of the switch transistor 234 is connected to VDD.

[0172] The gate terminal of the switch transistor 225 is connected to a select line SEL2. The one terminal of the switch transistor 235 is connected to MONITOR/DATA. The other terminal of the switch transistor 235 is connected to the driving transistor 233 and the anode electrode of the OLED 231. The anode electrode of the OLED 231 is connected to VDD.

[0173] The transistors 233 and 234 and the storage capacitor 232 are connected at node A6. The transistors 233 and 235 and the OLED 231 are connected at node B5.

[0174] The pixel circuit 230 is similar to the pixel circuit 190 of Figure 14. However, in the pixel circuit 230, the MONITOR/DATA line is used for monitoring and programming purpose.

[0175] Referring to Figures 21-22, the operation of Figure 22 includes operating cycles X91, X92 and X93.

[0176] During the first operating cycle X91, SEL1 and SEL2 are high and VDD goes to zero. The gate-source voltage of the driving transistor (e.g. 233 of Figure 21) becomes zero.

[0177] During the second operating cycle X92, a current (voltage) is applied to the OLED (e.g. 231 of Figure 21) through the MONITOR/DATA line, and its voltage (current) is extracted. As described above, the shift in the OLED voltage is extracted using the algorithm presented in Figure 10 or 11 based on the monitored voltage or current. This waveform can be combined with any other driving waveform.

[0178] The operating cycle X93 can be any operating cycle including the programming cycle. This depends on the status of the panel after OLED extraction.

[0179] The OLED voltage can be extracted during the driving cycle of the pixel circuit 230 of Figure 21 after it is programmed for a constant current using any driving technique. During the driving cycle the SEL2 goes to a high voltage, and so the voltage of the OLED can be read back through the MONITOR/DATA line for a specific pixel current.

[0180] As reported, the OLED characteristics improve under negative bias stress. As a result, a negative bias related to the stress history of the pixel, extracted from the OLED voltage/current, can be applied to the OLED during the time in which the display is not operating. This method can be used for any pixel circuit presented herein.

[0181] Using the OLED voltage/current extraction technique, a pixel circuit can provide stable brightness that is independent of pixel aging under prolonged display operation, to efficiently improve the display operating lifetime.

[0182] A technique for reducing the unwanted emission in a display array having a light emitting device in accordance with an embodiment of the present invention is described in detail. This technique includes removing OLED from a programming path during a programming cycle. This technique can be adopted in hybrid driving technique to extract information on the precise again of a pixel, e.g. the actual threshold voltage shift/mismatch of the driving transistor. The light emitting device is turned off during the programming/calibration cycle so that it prevents the unwanted emission and effect of the light emitting device on the pixel aging. This technique can be applied to any current mirror pixel circuit fabricated in any technology including poly silicon, amorphous silicon, crystalline silicon, and organic materials.

[0183] Figure 23 illustrates a mirror based pixel circuit 250 to which a technique for removing OLED from a programming path during a programming cycle is applied. The pixel circuit 250 includes an OLED 251, a storage capacitor 252, a programming transistor 253, a driving transistor 254, and switch transistors 255 and 256. The gate terminals of the transistors 253 and 254 are connected to IDATA through the switch transistors 255 and 256.

[0184] The transistors 253, 254, 255 and 256 are n-type TFTs. However, the transistors 253, 254, 255 and 256 maybe p-type TFTs. The OLED removing technique applied to the pixel circuit 250 is also applicable to a pixel circuit having p-type transistors. The transistors 253, 254, 255 and 256 may be fabricated using amorphous silicon, nano/micro crystalline silicon, poly silicon, organic semiconductors technologies (e.g. organic TFT), NMOS/PMOS technology or CMOS technology (e.g. MOSFET).

[0185] The transistors 253, 254 and 256 and the storage capacitor 252 are connected at node A10. The transistors 253 and 254, the OLED 251 and the storage capacitor 252 are connected at node B10.

[0186] In the conventional current programming, SEL goes high, and a programming current (IP) is applied to IDATA. Considering that the width of the mirror transistor 253 is "m" times larger than the width of the mirror transistor 254, the current flowing through the OLED 251 during the programming cycle is (m+1)IP. When "m" is large to gain significant speed improvement, the unwanted emission may become considerable.

[0187] By contrast, according to the OLED removing technique, VDD is brought into a lower voltage. This ensures the OLED 251 to be removed from a programming path as shown in Figure 24.

[0188] During a programming cycle, SEL is high and VDD goes to a reference voltage (Vref) in which the OLED 251 is reversely biased. Therefore, the OLED 251 is removed from the current path during the programming cycle.

[0189] During the programming cycle, the pixel circuit 250 may be programmed with scaled current through IDATA without experiencing unwanted emission.

[0190] During the programming cycle, the pixel circuit 250 may be programmed with current and using one of the techniques describe above. The voltage of the IDATA line is read back to extract the threshold voltage of the mirror transistor 253 which is the same as threshold voltage of the driving transistor 254.

[0191] Also, during the programming cycle, the pixel circuit 250 may be programmed with voltage through the IDATA line, using one of the techniques describe above. The current of the IDATA line is read back to extract the threshold voltage of the mirror transistor 253 which is the same as threshold voltage of the driving transistor 254.

[0192] The reference voltage Vref is chosen so that the voltage at node B10 becomes smaller than the ON voltage of the OLED 251. As a result, the OLED 251 turns off and the unwanted emission is zero. The voltage of the IDATA line includes

$$V_P + V_T + \Delta V_T \dots (3)$$

where V_P includes the drain-source voltage of the driving transistor 254 and the gate-source voltage of the transistor 253, V_T is the threshold voltage of the transistor 253 (254), and ΔV_T is the V_T shift/mismatch.

[0193] At the end of the programming cycle, VDD goes to its original value, and so voltage at node B10 goes to the OLED voltage V_{OLED} . At the driving cycle, SEL is low. The gate voltage of the transistor 254/253 is fixed and stored in the storage capacitor 252, since the switch transistors 255 and 256 are off. Therefore, the pixel current during the driving cycle becomes independent of the threshold voltage V_T .

[0194] The OLED removing technique can be adopted in hybrid driving technique to extract the V_T -shift or V_T -mismatch. From (3), if the pixel is programmed with the current, the only variant parameter in the voltage of the IDATA line is the V_T shift/mismatch (ΔV_T). Therefore, ΔV_T can be extracted and the programming data can be calibrated with ΔV_T .

[0195] Figure 25 illustrates an example of a system architecture for implementing the OLED removing technique. A display array 260 includes a plurality of pixel circuits, e.g. pixel circuit 250 of Figure 26. A display controller and scheduler 262 controls and schedules the operation of the display array 260. A driver 264 provides operation voltages to the pixel circuit. The driver provides the operation voltage(s) to the pixel circuit based on instructions/commands from the display controller and scheduler 262 such that the OLED is removed from a programming path of the pixel circuit, as described above.

[0196] The controller and scheduler 262 may include functionality of the display controller and scheduler 64 of Figure 3, or may include functionality of the data process and calibration unit 206 of Figure 16. The system of Figure 25 may have any of these functionalities, the calibration-scheduling described above, the voltage/current extraction described above, or combinations thereof

[0197] The simulation result for the voltage on IDATA line for different V_T is illustrated in Figure 26. Referring to Figures 23-26, the voltage of the IDATA line includes the shift in the threshold voltage of the transistors 253 and 254. The programming current is 1 μA .

[0198] The unwanted emission is reduced significantly resulting in a higher resolution. Also, individual extraction of circuit aging and light emitting device aging become possible, leading in a more accurate calibration.

[0199] It is noted that each of the transistors shown in Figures 4-8, 14, 20, 21, 23 and 24 can be replaced with a p-type transistor using the concept of complementary circuits.

[0200] The present invention has been described with regard to one or more embodiments. However, it will be apparent to persons skilled in the art that a number of variations and modifications can be made without departing from the scope of the invention as defined in the claims.

Claims

1. A method of real-time calibration for a display array (10) having a plurality of pixels (12) arranged in rows and columns, wherein each pixel comprises a plurality of transistors and a light emitting element, each pixel being selected by a select line connected to the respective row of the pixel and being driven by a data line connected the respective column of the pixel, the method comprising the steps of:

generating a priority list of pixels associating calibration priorities with one or more pixels (12) from the plurality of pixels in the display array (10), the calibration priorities of the one or more pixels in the priority list being ordered according to a brightness of the one or more pixels, each of the one or more pixels listed in the priority list having a respective programming current that is larger than a reference current;

selecting n pixels from the priority list for a selected column of the display array (S8), the n selected pixels having the highest calibration priorities in the priority list, wherein the number n is selected based on a display size N , the display size N being the number of pixels of the display array, and expected instability in device characteristics with time, said instability in device characteristics with time being a shift in characteristics of at least one of the transistors and the light emitting element, in such a manner so that

$$n > \frac{KtN}{e}$$

where:

K is the highest rate in said shift in characteristics for all pixels of the display array;
 t is the length of a programming cycle required for programming a column of the display array; and
 e is the allowable error in said shift in characteristics for all pixels of the display array;

enabling a calibration mode for the n selected pixels and a normal operation mode for the rest of the pixels in the selected column (S10);

programming the pixels in the selected column with a corresponding programming voltage, wherein the programming voltage for the pixels other than the n selected pixels in the selected column is adjusted based on compensation data stored in a compensation memory (34);

monitoring a current flowing through the n selected pixels;
 comparing the monitored current with an expected current value, and generating calibration data for the n selected pixels;
 updating the compensation data in the compensation memory (34) based on the calibration data; and
 updating the priority list by associating a lowest calibration priority with each of the n selected pixels.

2. A method according to claim 1, wherein the priority list is an ordered list with the highest calibration priority pixel at the top, and wherein the step of updating the priority list comprises:

moving the selected one or more pixels to the bottom of the priority list.

3. A method according to claim 1 or claim 2, wherein the step of monitoring comprises:

coupling (38) the column to a monitor (40, 42, 44, 48) for monitoring a voltage associated with the current on a data line (16).

4. A method according to claim 3, wherein the step of updating comprises:

comparing (46) the monitored voltage with an expected voltage (48) corresponding to the expected current value.

5. A method according to any one of claims 1-4, wherein the n selected pixels have a programming current above a threshold current (I_{th}).

6. A method according to any one of claims 1-5, wherein if each programming cycle takes a time $t = 1/(f \times m_2)$ and the total number of pixels $N = \alpha \times m_1 \times m_2$, the number n of the selected pixels is:

$$n > \frac{\alpha K m_1}{f e}$$

where:

α is the number of light emitting elements per pixel;
 m_1 is the number of rows in the display array; and
 f is the refresh frequency of the display array.

7. A method according to claim 6, wherein α is preferably 3 or 4, or α is 1 or 2.

8. A system for real-time calibration for a display array (10) having a plurality of pixels (12) arranged in rows and columns, wherein each pixel comprises a plurality of transistors and a light emitting element, each pixel being selected by a select line connected to the respective row of the pixel and being driven by a data line connected the respective column of the pixel, the system comprising:

a calibration scheduler (32) for selecting n pixels for a selected column of the display array from a priority list, the calibration scheduler (32) being adapted to enable a calibration mode for the n selected pixels, and a normal operation mode for the other pixels in the column,
 wherein the priority list associates calibration priorities with one or more pixels (12) from the plurality of pixels, the calibration priorities of the one or more pixels in the priority list being ordered according to a brightness of the one or more pixels, each of the one or more pixels listed in the priority list having a respective programming current that is larger than a reference current, and
 wherein the n selected pixels have the highest calibration priorities in the priority list, the number n being selected based on a display size, the display size N being the number of pixels of the display array, and expected instability in device characteristics with time, said instability in device characteristics with time being a shift in characteristics of at least one of the transistors and the light emitting element, in such a manner so that

$$n > \frac{KtN}{e}$$

where:

K is the highest rate in said shift in characteristics for all pixels of the display array;
 t is the length of a programming cycle required for programming a column of the display array; and
 e is the allowable error in said shift in characteristics for all pixels of the display array;

a compensation memory (34) for storing compensation data;
a driver (28) for driving a data line (16) connected to the selected column and programming the pixels in the column with a corresponding programming voltage, wherein the programming voltage for the pixels other than the n selected pixels in the selected column is adjusted based on the compensation data stored in the compensation memory;
a monitor (40, 42, 44, 48) for monitoring a current flowing through the n selected pixels; and
a generator (46) for comparing the monitored current with an expected current value, generating calibration data for the n selected pixels, and updating the compensation data based on the calibration data;
wherein the priority list is updated by associating a lowest calibration priority with each of the n selected pixels.

9. A system according to claim 8, comprising:

a switch (38) for each column, for selectively connecting the corresponding column to the monitor; and
a switch (36) for each column, for selectively connecting the corresponding column to the driver (28).

10. A system according to claim 8 or 9, wherein the monitor includes:

a sensor (40, 42) for sensing a voltage associated with the current, and
a translator (48) for translating a data input to a voltage corresponding to the expected current value,

and wherein the generator comprises:

a comparator (46) for comparing the sensed voltage with the voltage from the translator (48).

11. A system according to claim 10, wherein the monitor includes a switch (38) for each column, for selectively connecting the corresponding column to the sensor (40, 42).

12. A system according to claim 8, wherein the driver (28) is coupled to a pixel in the calibration mode via the monitor (40, 42).

13. A system according to claim 8 or claim 12, wherein the display array (10) is connected to the driver (28), and wherein the driver (28) drives the pixels in the normal operation mode based on the programming voltage and a compensation voltage corresponding to the compensation data.

14. A system according to any one of claims 8 - 13, wherein the pixel (12) is a current programmed pixel circuit.

15. A system according to any one of claims 8 - 14, wherein the priority list is an ordered list with the highest calibration priority pixel at the top, and wherein the calibration scheduler updates the priority list by moving the n selected pixels to the bottom of the priority list.

16. A system according to any one of claims 8 - 15, wherein the n selected pixels have a programming current above a threshold current (I_{th}).

17. A system according to any one of claims 8 - 16, wherein if each programming cycle takes a time $t = 1 / (f \times m_2)$ and the total number of pixels $N = \alpha \times m_1 \times m_2$, the number n of the selected pixels is:

$$n > \frac{\alpha K m_1}{f e}$$

where:

α is the number of light emitting elements per pixel;
 m_1 is the number of rows in the display array; and
 f is the refresh frequency of the display array.

18. A system according to claim 17, wherein α is preferably 3 or 4, or α is 1 or 2.

19. A system according to any one of claims 8 - 18, wherein the display array is an AMOLED array.

20. A system according to any one of claims 8 - 19, wherein the pixel (12) comprises:

an organic light emitting diode.

21. A system according to any one of claims 8 - 20, wherein the pixel (12) comprises:

at least one thin film transistor.

22. A system according to any one of claims 8 - 21, wherein the pixel (12) comprises:

a n-type or a p-type thin film transistor.

Patentansprüche

1. Verfahren zur Echtzeit-Kalibrierung einer Anzeigefeld (10) mit einer Vielzahl von Pixeln (12), die in Zeilen und Spalten angeordnet sind, wobei jedes Pixel eine Vielzahl von Transistoren und ein lichtemittierendes Element umfasst, wobei jedes Pixel von einer Auswahlleitung ausgewählt wird, die mit der jeweiligen Pixelzeile verbunden ist und von einer Datenleitung angesteuert wird, die mit der jeweiligen Pixelspalte verbunden ist, wobei das Verfahren folgende Schritte umfasst:

Generieren einer Prioritätsliste von Pixeln, welche einem oder mehreren Pixeln (12) aus der Vielzahl von Pixeln in dem Anzeigefeld (10) Kalibrierungsprioritäten zuordnet, wobei die Kalibrierungsprioritäten der einen oder mehreren Pixel in der Prioritätsliste gemäß einer Helligkeit der einen oder mehreren Pixel geordnet sind, wobei jedes der einen oder mehreren in der Prioritätsliste gelisteten Pixel einen Programmierstrom hat, der größer als ein Referenzstrom ist;

Auswählen von n Pixeln aus der Prioritätsliste für eine ausgewählte Spalte des Anzeigefelds (S8), wobei die n ausgewählten Pixel die höchsten Kalibrierungsprioritäten in der Prioritätsliste haben, die Anzahl n basierend auf einer Anzeigegröße N ausgewählt wird, die Anzeigegröße N die Anzahl der Pixel des Anzeigefelds ist, und basierend auf einer erwarteten Instabilität in den Gerätemerkmalen über die Zeit, wobei die Instabilität in den Gerätemerkmalen über die Zeit eine Veränderung der Merkmale von mindestens einem der Transistoren und dem lichtemittierenden Element ist, auf solche Weise, dass

$$n > \frac{K t N}{e}$$

wobei:

K die höchste Rate der Veränderung der Merkmale für alle Pixel des Anzeigefelds ist;
 t die Länge eines zur Programmierung einer Spalte des Anzeigefelds erforderlichen Programmierzyklus

ist; und
e der zulässige Fehler in der Veränderung der Merkmale für alle Pixel des Anzeigefelds ist;

Freigabe eines Kalibrierungsmodus für die n ausgewählten Pixel und eines normalen Betriebsmodus für die restlichen Pixel in der ausgewählten Spalte (S10);

Programmieren der Pixel in der ausgewählten Spalte mit einer entsprechenden Programmierspannung, wobei die Programmierspannung für die anderen Pixel als die n ausgewählten Pixel in der ausgewählten Spalte basierend auf Kompensationsdaten eingestellt wird, die in einem Kompensationsspeicher (34) gespeichert sind; Überwachen eines Stroms, der durch die n ausgewählten Pixel fließt;

Vergleichen des überwachten Stroms mit einem erwarteten Stromwert, und Generieren von Kalibrierungsdaten für die n ausgewählten Pixel;

Aktualisieren der Kompensationsdaten in dem Kompensationsspeicher (34) auf Basis der Kalibrierungsdaten; und

Aktualisieren der Prioritätsliste durch Zuordnen einer niedrigsten Kalibrierungspriorität zu jedem der n ausgewählten Pixel.

2. Verfahren nach Anspruch 1, wobei die Prioritätsliste so geordnet ist, dass sich die Pixel mit der höchsten Kalibrierungspriorität oben befinden, und wobei der Schritt des Aktualisierens der Prioritätsliste umfasst:

Verschieben der ausgewählten einen oder mehreren Pixel zum Ende der Prioritätsliste.

3. Verfahren nach Anspruch 1 oder 2, wobei der Schritt des Überwachens umfasst:

Verbinden (38) der Spalte mit einem Überwachungsgerät (40, 42, 44, 48) zum Überwachen einer zu dem Strom an einer Datenleitung (16) gehörigen Spannung.

4. Verfahren nach Anspruch 3, wobei der Schritt des Aktualisierens umfasst:

Vergleichen (46) der überwachten Spannung mit einer erwarteten Spannung (48), die dem erwarteten Stromwert entspricht.

5. Verfahren nach einem der Ansprüche 1 - 4, wobei die n ausgewählten Pixel einen Programmierstrom oberhalb eines Schwellenstroms (I_{th}) haben.

6. Verfahren nach einem der Ansprüche 1 - 5, wobei, wenn jeder Programmierzyklus eine Zeit $t = 1/(f \times m_2)$ benötigt und die Gesamtzahl der Pixel $N = \alpha \times m_1 \times m_2$, beträgt, die Anzahl n der ausgewählten Pixel lautet:

$$n > \frac{\alpha K m_1}{f e}$$

wobei:

α die Anzahl der lichtemittierenden Elemente pro Pixel ist;
 m_1 die Anzahl der Zeilen in dem Anzeigefeld ist; und
 f die Bildwiederholfrequenz des Anzeigefelds ist.

7. Verfahren nach Anspruch 6, wobei α vorzugsweise 3 oder 4 ist, oder α 1 oder 2 ist.

8. System zur Echtzeit-Kalibrierung eines Anzeigefelds (10) mit einer Vielzahl von Pixeln (12), die in Zeilen und Spalten angeordnet sind, wobei jedes Pixel eine Vielzahl von Transistoren und ein lichtemittierendes Element umfasst, wobei jedes Pixel von einer Auswahlleitung ausgewählt wird, die mit der jeweiligen Pixelzeile verbunden ist und von einer Datenleitung angesteuert wird, die mit der jeweiligen Pixelspalte verbunden ist, wobei das System umfasst:

eine Kalibrierungsablaufsteuerung (32) zum Auswählen der n Pixel für eine ausgewählten Zeile des Anzeigefelds aus einer Prioritätsliste, wobei die Kalibrierungsablaufsteuerung (32) dazu eingerichtet ist, einen Kalibrierungsmodus für die n ausgewählten Pixel und einen normalen Betriebsmodus für die anderen Pixel in der Spalte

freizugeben,

wobei die Prioritätsliste einem oder mehreren Pixeln (12) aus der Vielzahl von Pixeln Kalibrierungsprioritäten zuordnet, die Kalibrierungsprioritäten der einen oder mehreren Pixel in der Prioritätsliste gemäß einer Helligkeit der einen oder mehreren Pixel geordnet sind, wobei jedes der einen oder mehreren in der Prioritätsliste gelisteten Pixel einen Programmierstrom hat, der größer als ein Referenzstrom ist; und
wobei die n ausgewählten Pixel die höchsten Kalibrierungsprioritäten in der Prioritätsliste aufweisen, wobei die Anzahl n basierend auf einer Anzeigegröße ausgewählt wird, die Anzeigegröße N die Anzahl der Pixel in dem Anzeigefeld ist, und basierend auf einer erwarteten Instabilität in den Gerätemerkmalen über die Zeit, wobei die Instabilität in den Gerätemerkmalen über die Zeit eine Veränderung der Merkmale von mindestens einem der Transistoren und dem lichtemittierenden Element ist, auf solche Weis, dass

$$n > \frac{KtN}{e}$$

wobei:

K die höchste Rate der Veränderung der Merkmale für alle Pixel des Anzeigefelds ist;
t die Länge eines zur Programmierung einer Spalte des Anzeigefelds erforderlichen Programmierzyklus ist; und
e der zulässige Fehler in der Veränderung der Merkmale für alle Pixel des Anzeigefelds ist;

einen Kompensationsspeicher (34) zu Speichern von Kompensationsdaten;
einen Treiber (28) zum Ansteuern einer Datenleitung (16), die mit der ausgewählten Spalte verbunden ist, und zum Programmieren der Pixel in der Spalte mit einer entsprechenden Programmiervoltage, wobei die Programmiervoltage für die anderen Pixel als die n ausgewählten Pixel in der ausgewählten Spalte basierend auf Kompensationsdaten eingestellt wird, die in dem Kompensationsspeicher gespeichert sind;
ein Überwachungsgerät (40, 42, 44, 48) zum Überwachen eines Stroms, der durch die n ausgewählten Pixel fließt; und
einen Generator (46) zum Vergleichen des überwachten Stroms mit einem erwarteten Stromwert, zum Generieren von Kalibrierungsdaten für die n ausgewählten Pixel und zum Aktualisieren der Kompensationsdaten basierend auf den Kalibrierungsdaten;
wobei die Prioritätsliste durch Zuordnen einer niedrigsten Kalibrierungspriorität zu jedem der n ausgewählten Pixel aktualisiert wird.

9. System nach Anspruch 8, das umfasst:

einen Schalter (38) für jede Spalte zum selektiven Verbinden der entsprechenden Spalte mit dem Überwachungsgerät; und
einen Schalter (36) für jede Spalte zum selektiven Verbinden der entsprechenden Spalte mit dem Treiber (28).

10. System nach Anspruch 8 oder 9, wobei das Überwachungsgerät umfasst:

einen Sensor (40, 42) zum Messen einer zu dem Strom gehörigen Spannung, und
einen Übersetzer (48) zum Übersetzen einer Dateneingabe in eine Spannung, die dem erwarteten Stromwert entspricht,
und wobei der Generator umfasst:

eine Vergleichseinrichtung (46) zum Vergleichen der gemessenen Spannung mit der Spannung von dem Übersetzer (48).

11. System nach Anspruch 10, wobei das Überwachungsgerät einen Schalter (38) für jede Spalte aufweist, um die entsprechende Spalte selektiv mit dem Sensor (40, 42) zu verbinden.

12. System nach Anspruch 8, wobei der Treiber (28) im Kalibrierungsmodus über das Überwachungsgerät (40, 42) mit einem Pixel verbunden ist.

13. System nach Anspruch 8 oder 12, wobei das Anzeigefeld (10) mit dem Treiber (28) verbunden ist, und wobei der Treiber (28) die Pixel im normalen Betriebsmodus basierend auf der Programmierspannung und einer den Kompensationsdaten entsprechenden Kompensationsspannung ansteuert.

14. System nach einem der Ansprüche 8 - 13, wobei das Pixel (12) eine stromprogrammierte Pixelschaltung ist.

15. System nach einem der Ansprüche 8 - 14, wobei die Prioritätsliste so geordnet ist, dass sich das Pixel mit der höchsten Kalibrierungspriorität oben befindet, und wobei die Kalibrierungsablaufsteuerung die Prioritätsliste durch Verschieben der n ausgewählten Pixel zum Ende der Prioritätsliste aktualisiert.

16. System nach einem der Ansprüche 8 - 15, wobei die n ausgewählten Pixel einen Programmierstrom oberhalb eines Schwellenstroms (I_{th}) haben.

17. System nach einem der Ansprüche 8 - 16, wobei, wenn jeder Programmierzyklus eine Zeit $t = 1/(f \times m_2)$ benötigt und die Gesamtzahl der Pixel $N = \alpha \times m_1 \times m_2$, beträgt, die Anzahl n der ausgewählten Pixel lautet:

$$n > \frac{\alpha K m_1}{f e}$$

wobei:

α die Anzahl der lichtemittierenden Elemente pro Pixel ist;
 m_1 die Anzahl der Zeilen in dem Anzeigefeld ist; und
 f die Bildwiederholfrequenz des Anzeigefelds ist.

18. System nach Anspruch 17, wobei α vorzugsweise 3 oder 4 ist, oder α 1 oder 2 ist.

19. System nach einem der Ansprüche 8 - 18, wobei das Anzeigefeld eine AMOLED-Anordnung ist.

20. System nach einem der Ansprüche 8 - 19, wobei das Pixel (12) umfasst:

eine organische lichtemittierende Diode.

21. System nach einem der Ansprüche 8 - 20, wobei das Pixel (12) umfasst:

mindestens einen Dünnschichttransistor.

22. System nach einem der Ansprüche 8 - 21, wobei das Pixel (12) umfasst: einen n-Typ oder p-Typ Dünnschichttransistor.

Revendications

1. Procédé d'étalonnage en temps réel d'une matrice d'affichage (10) comportant une pluralité de pixels (12) agencés en rangées et en colonnes, dans lequel chaque pixel comprend une pluralité de transistors et un élément électroluminescent, chaque pixel étant sélectionné par une ligne de sélection connectée à la rangée respective du pixel et étant piloté par une ligne de données connectée à la colonne respective du pixel, le procédé comprenant les étapes consistant à :

générer une liste de priorité de pixels associant des priorités d'étalonnage avec un ou plusieurs pixels (12) de la pluralité de pixels de la matrice d'affichage (10), les priorités d'étalonnage du ou des pixels dans la liste de priorité étant ordonnées en fonction de la luminosité du ou des pixels, chacun du ou des pixels énuméré(s) dans la liste de priorité ayant un courant de programmation respectif supérieur à un courant de référence ;
sélectionner n pixels de la liste de priorité pour une colonne sélectionnée de la matrice d'affichage (S8), les n pixels sélectionnés ayant les priorités d'étalonnage les plus hautes dans la liste de priorité, dans lequel le

nombre n est sélectionné en se basant sur une dimension de l'affichage N , la dimension de l'affichage N étant le nombre de pixels de la matrice d'affichage, et une instabilité attendue des caractéristiques du dispositif par rapport au temps, ladite instabilité des caractéristiques du dispositif par rapport au temps étant un décalage des caractéristiques d'au moins l'un des transistors et l'élément électroluminescent, de telle manière que

$$n > \frac{KtN}{e}$$

où :

K est la vitesse la plus élevée dudit décalage des caractéristiques pour tous les pixels de la matrice d'affichage ;

t est la longueur d'un cycle de programmation nécessaire pour programmer une colonne de la matrice d'affichage ; et

e est l'erreur admissible dans ledit décalage des caractéristiques pour tous les pixels de la matrice d'affichage ;

activer un mode d'étalonnage pour les n pixels sélectionnés et un mode de fonctionnement normal pour le reste des pixels dans la colonne sélectionnée (S10) ;

programmer les pixels dans la colonne sélectionnée avec une tension de programmation correspondante, dans lequel la tension de programmation pour les pixels autre que les n pixels sélectionnés dans la colonne sélectionnée est réglée en se basant sur des données de compensation enregistrées dans la mémoire de compensation (34) ;

surveiller le courant circulant à travers les n pixels sélectionnés ;

comparer le courant surveillé avec une valeur de courant attendue, et générer des données d'étalonnage pour les n pixels sélectionnés ;

mettre à jour les données de compensation dans la mémoire de compensation (34) en se basant sur les données d'étalonnage ; et

mettre à jour la liste de priorité en associant une priorité d'étalonnage la plus basse avec chacun des n pixels sélectionnés.

2. Procédé selon la revendication 1, dans lequel la liste de priorité est une liste ordonnée, le pixel de priorité d'étalonnage la plus haute étant au sommet et dans lequel l'étape de mise à jour de la liste de priorité comprend :

le déplacement du ou des pixels sélectionnés vers le bas de la liste de priorité.

3. Procédé selon la revendication 1 ou la revendication 2, dans lequel l'étape de surveillance comprend :

le couplage (38) de la colonne à un moniteur (40, 42, 44, 48) pour surveiller une tension associée au courant sur une ligne de données (16).

4. Procédé selon la revendication 3, dans lequel l'étape de mise à jour comprend :

la comparaison (46) de la tension surveillée avec une tension attendue (48) correspondant à la valeur de courant attendue.

5. Procédé selon l'une quelconque des revendications 1 à 4, dans lequel les n pixels sélectionnés ont un courant de programmation supérieur à un courant de seuil (I_{th}).

6. Procédé selon l'une quelconque des revendications 1 à 5, dans lequel, si chaque cycle de programmation s'effectue en un temps $t = 1 / (f \times m_2)$ et que le nombre total de pixels $N = \alpha \times m_1 \times m_2$, le nombre n de pixels sélectionnés est égal à :

$$n > \frac{\alpha K m_1}{f e}$$

où :

- est le nombre d'éléments électroluminescents par pixel ;
- m_1 est le nombre de rangées de la matrice d'affichage ; et
- f est la fréquence de rafraîchissement de la matrice d'affichage.

7. Procédé selon la revendication 6, dans lequel α est de préférence égal à 3 ou 4, ou α est égal à 1 ou 2.

8. Système d'étalonnage en temps réel d'une matrice d'affichage (10) comportant une pluralité de pixels (12) agencés en rangées et en colonnes, dans lequel chaque pixel comprend une pluralité de transistors et un élément électroluminescent, chaque pixel étant sélectionné par une ligne de sélection connectée à la rangée respective du pixel et étant piloté par une ligne de données connectée à la colonne respective du pixel, le système comprenant :

un planificateur d'étalonnage (32) pour sélectionner n pixels pour une colonne sélectionnée de la matrice d'affichage à partir d'une liste de priorité, le planificateur d'étalonnage (32) étant adapté à activer un mode d'étalonnage pour les n pixels sélectionnés et un mode de fonctionnement normal pour les autres pixels de la colonne, dans lequel la liste de priorité associe des priorités d'étalonnage avec un ou plusieurs pixels (12) de la pluralité de pixels, les priorités d'étalonnage du ou des pixels dans la liste de priorité étant ordonnées en fonction de la luminosité du ou des pixels, chacun du ou des pixels énuméré(s) dans la liste de priorité ayant un courant de programmation respectif supérieur à un courant de référence ; et dans lequel les n pixels sélectionnés ont les priorités d'étalonnage les plus hautes dans la liste de priorité, le nombre n étant sélectionné en se basant sur la dimension de l'affichage, la dimension de l'affichage N étant le nombre de pixels de la matrice d'affichage, et une instabilité attendue des caractéristiques du dispositif par rapport au temps, ladite instabilité des caractéristiques du dispositif par rapport au temps étant un décalage des caractéristiques d'au moins l'un des transistors et l'élément électroluminescent, de telle manière que

$$n > \frac{KtN}{e}$$

où :

K est la vitesse la plus élevée dudit décalage des caractéristiques pour tous les pixels de la matrice d'affichage ;
 t est la longueur d'un cycle de programmation nécessaire pour programmer une colonne de la matrice d'affichage ; et
 e est l'erreur admissible dans ledit décalage des caractéristiques pour tous les pixels de la matrice d'affichage ;

une mémoire de compensation (34) pour enregistrer des données de compensation ;
 un pilote (28) pour piloter une ligne de données (16) connectée à la colonne sélectionnée et pour programmer les pixels dans la colonne avec une tension de programmation correspondante, dans lequel la tension de programmation pour les pixels autre que les n pixels sélectionnés dans la colonne sélectionnée est réglée en se basant sur les données de compensation enregistrées dans la mémoire de compensation ;
 un moniteur (40, 42, 44, 48) pour surveiller le courant circulant à travers les n pixels sélectionnés ; et
 un générateur (46) pour comparer le courant surveillé avec une valeur de courant attendue, générer des données d'étalonnage pour les n pixels sélectionnés, et mettre à jour les données de compensation en se basant sur les données d'étalonnage ;
 dans lequel la liste de priorité est mise à jour en associant une priorité d'étalonnage la plus basse avec chacun des n pixels sélectionnés.

9. Système selon la revendication 8, comprenant :

un commutateur (38) pour chaque colonne, pour connecter de façon sélective la colonne correspondante au moniteur ; et
 un commutateur (36) pour chaque colonne, pour connecter de façon sélective la colonne correspondante au

pilote (28).

10. Système selon la revendication 8 ou 9, dans lequel le moniteur comporte :

un détecteur (40, 42) pour détecter une tension associée au courant, et
un traducteur (48) pour traduire une entrée de données en une tension correspondant à la valeur de courant attendu,
et dans lequel le générateur comprend :

un comparateur (46) pour comparer la tension détectée avec la tension du traducteur (48).

11. Système selon la revendication 10, dans lequel le moniteur comporte un commutateur (38) pour chaque colonne, pour connecter de façon sélective la colonne correspondante au détecteur (40, 42).

12. Système selon la revendication 8, dans lequel le pilote (28) est couplé à un pixel dans le mode d'étalonnage par l'intermédiaire du moniteur (40, 42).

13. Système selon la revendication 8 ou la revendication 12, dans lequel la matrice d'affichage (10) est connectée au pilote (28), et dans lequel le pilote (28) pilote les pixels dans le mode de fonctionnement normal en se basant sur la tension de programmation et sur une tension de compensation correspondant aux données de compensation.

14. Système selon l'une quelconque des revendications 8 à 13, dans lequel le pixel (12) est un circuit de pixel programmé par un courant.

15. Système selon l'une quelconque des revendications 8 à 14, dans lequel la liste de priorité est une liste ordonnée, le pixel de priorité d'étalonnage la plus haute étant au sommet, et dans lequel le planificateur d'étalonnage met à jour la liste de priorité en déplaçant les n pixels sélectionnés vers le bas de la liste de priorité.

16. Système selon l'une quelconque des revendications 8 à 15, dans lequel les n pixels sélectionnés ont un courant de programmation supérieur à un courant de seuil (I_{th}).

17. Système selon l'une quelconque des revendications 8 à 16, dans lequel, si chaque cycle de programmation s'effectue en un temps $t = 1/(f \times m_2)$ et que le nombre total de pixels $N = \alpha \times m_1 \times m_2$, le nombre n de pixels sélectionnés est égal à :

$$n > \frac{\alpha K m_1}{f e}$$

où :

- est le nombre d'éléments électroluminescents par pixel ;
- m_1 est le nombre de rangées de la matrice d'affichage ; et
- f est la fréquence de rafraîchissement de la matrice d'affichage.

18. Système selon la revendication 17, dans lequel α est de préférence égal à 3 ou 4, ou α est égal à 1 ou 2.

19. Système selon l'une quelconque des revendications 8 à 18, dans lequel la matrice d'affichage et une matrice AMOLED.

20. Système selon l'une quelconque des revendications 8 à 19, dans lequel le pixel (12) comprend :

une diode électroluminescente organique.

21. Système selon l'une quelconque des revendications 8 à 20, dans lequel le pixel (12) comprend :

au moins un transistor en couches minces.

- 22.** Système selon l'une quelconque des revendications 8 à 21, dans lequel le pixel (12) comprend :
- un transistor en couches minces de type n ou de type p.

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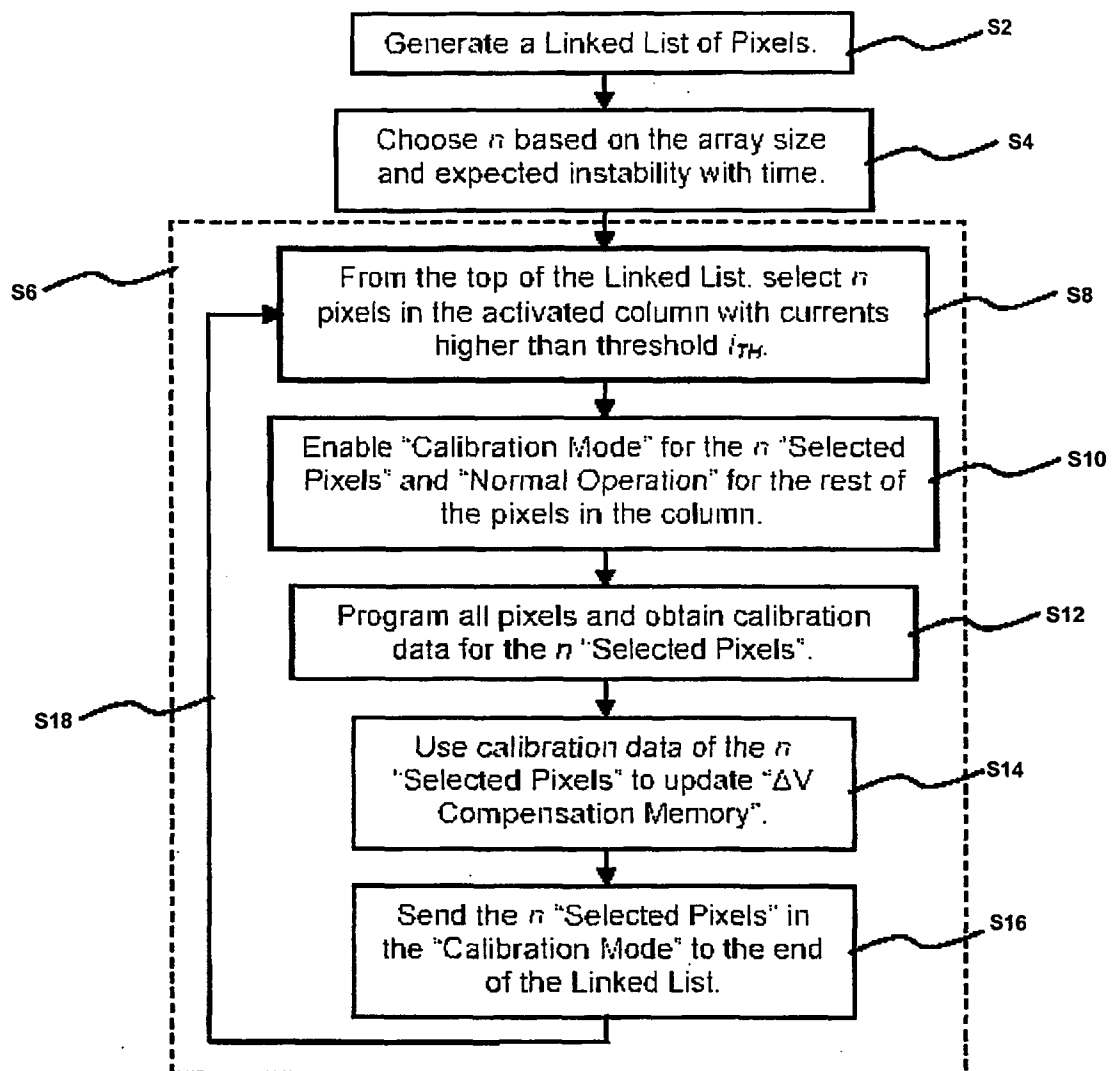
35

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**FIG.1**

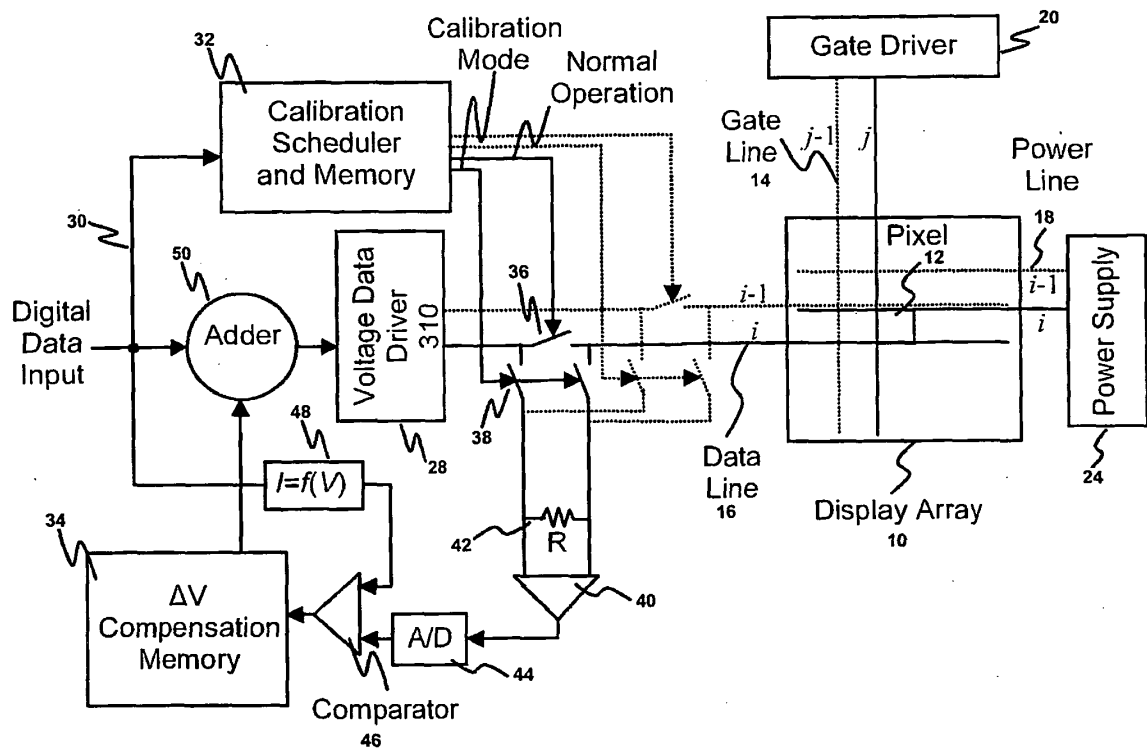


FIG. 2

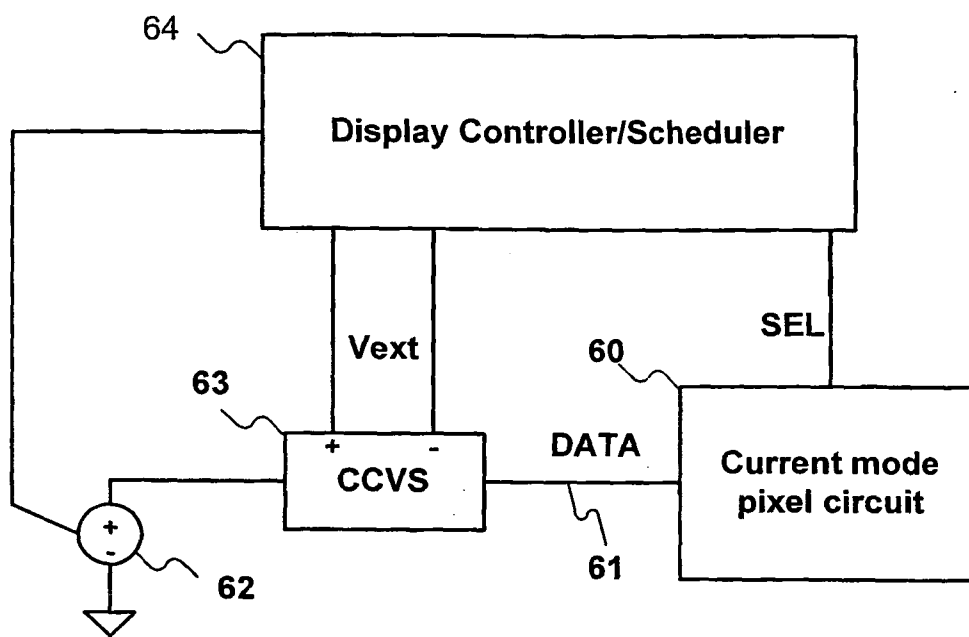


FIG.3

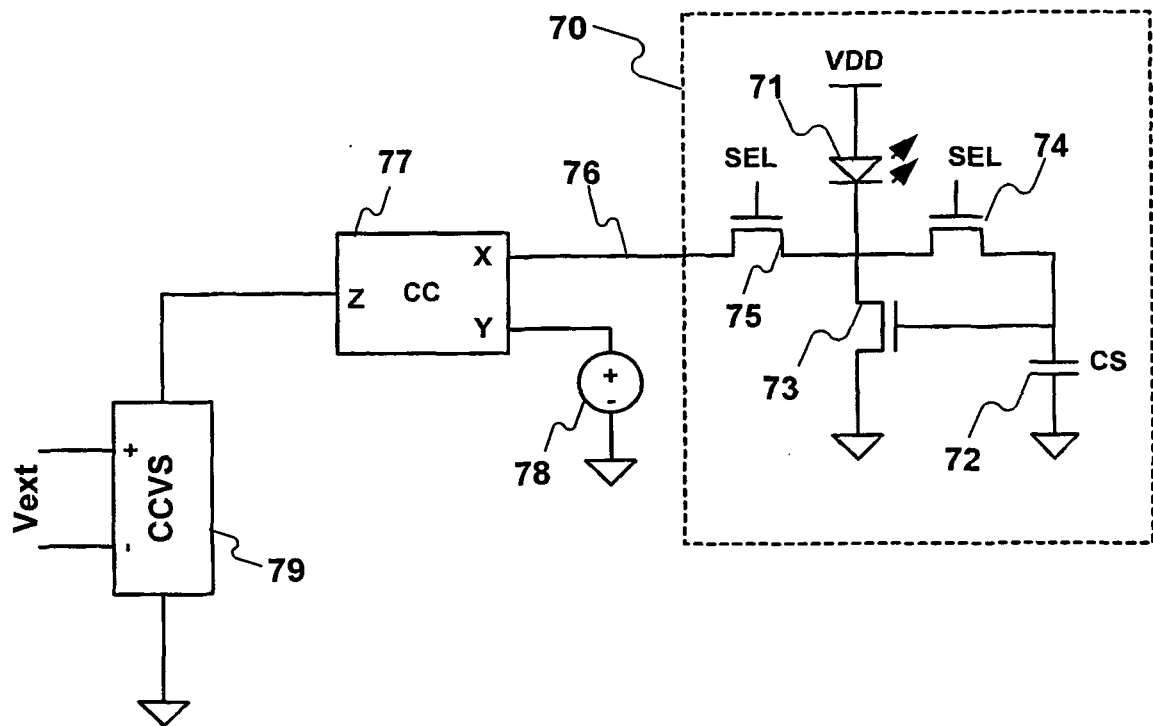


FIG.4

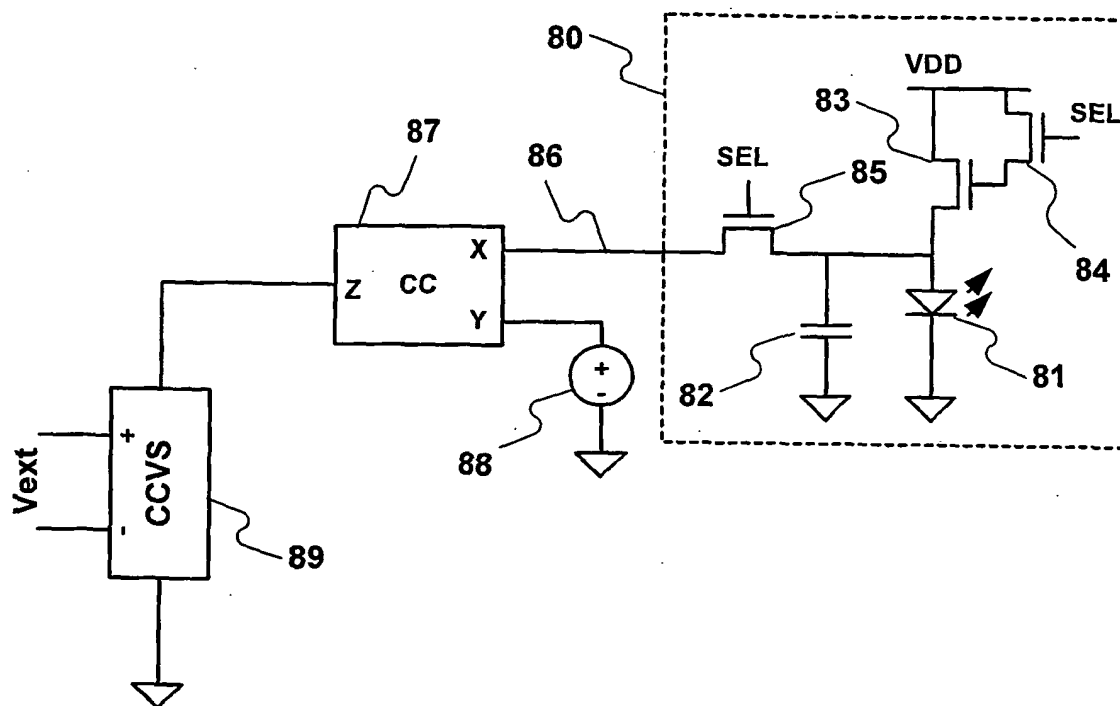


FIG.5

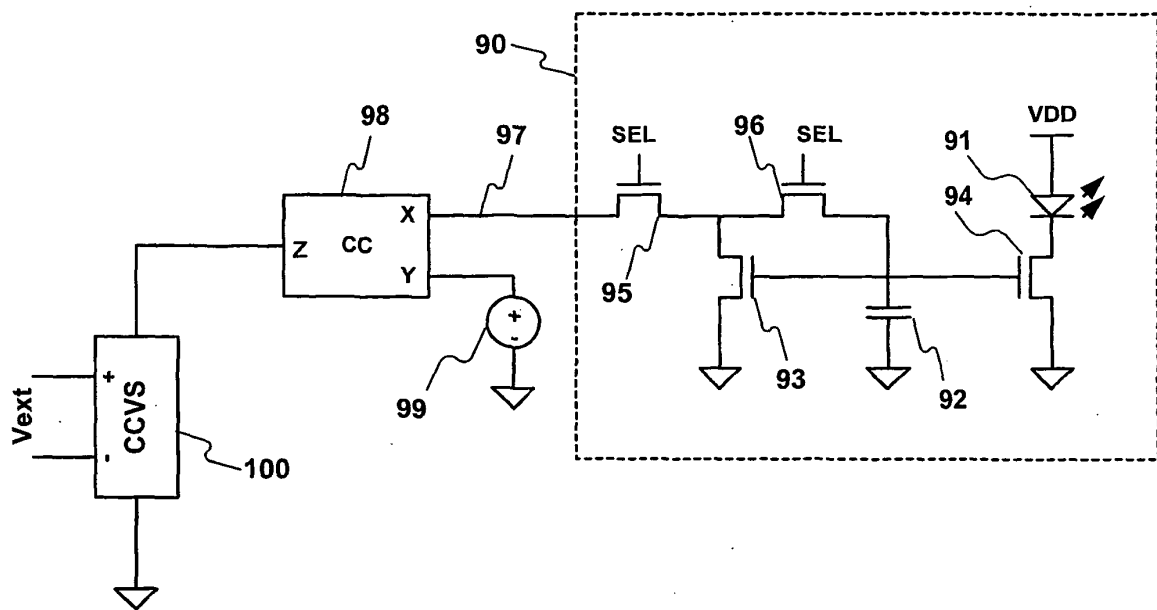


FIG. 6

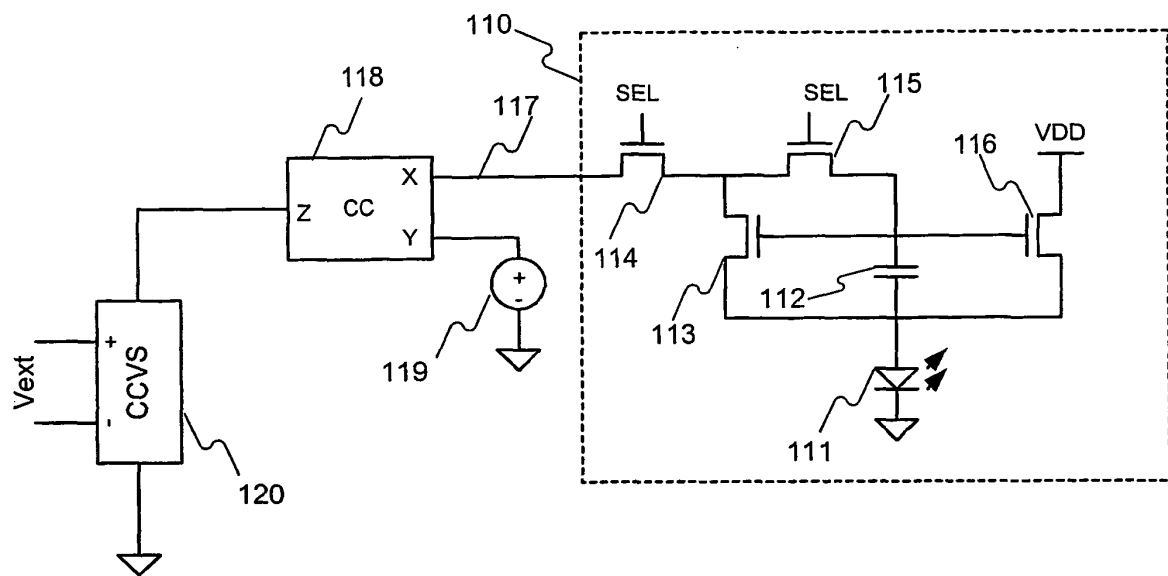


FIG. 7

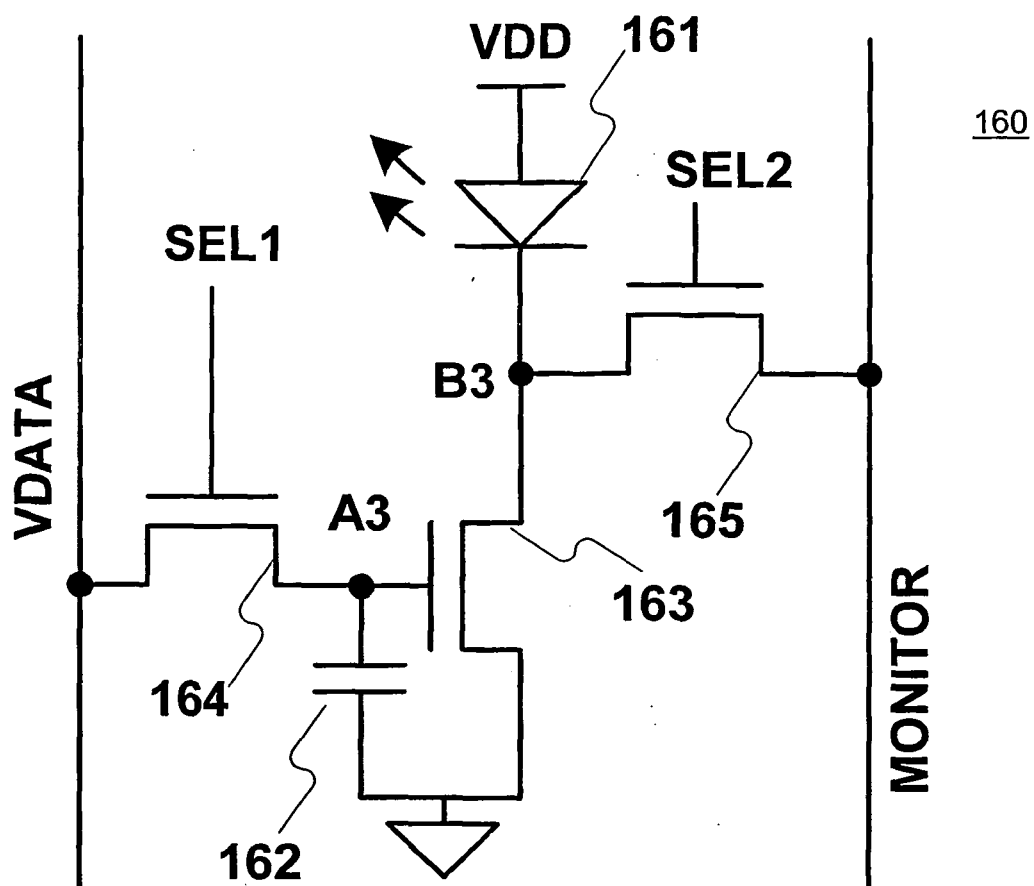


FIG. 8

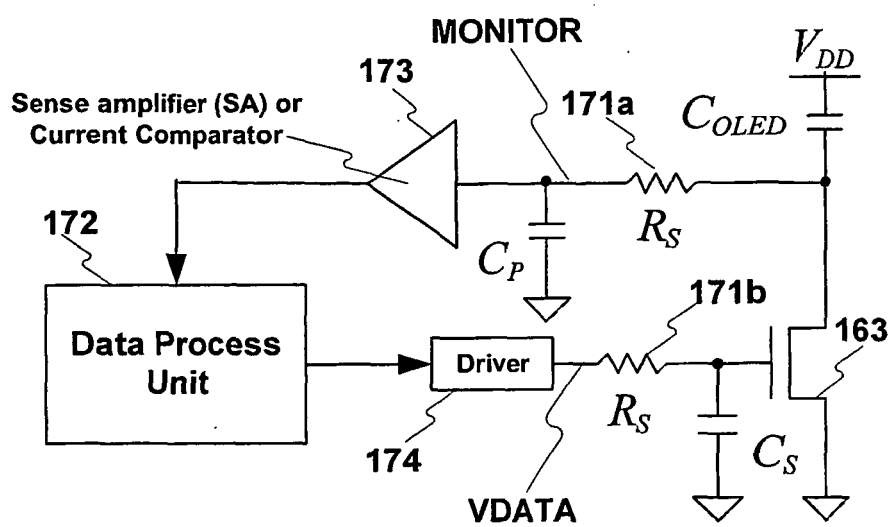


FIG. 9

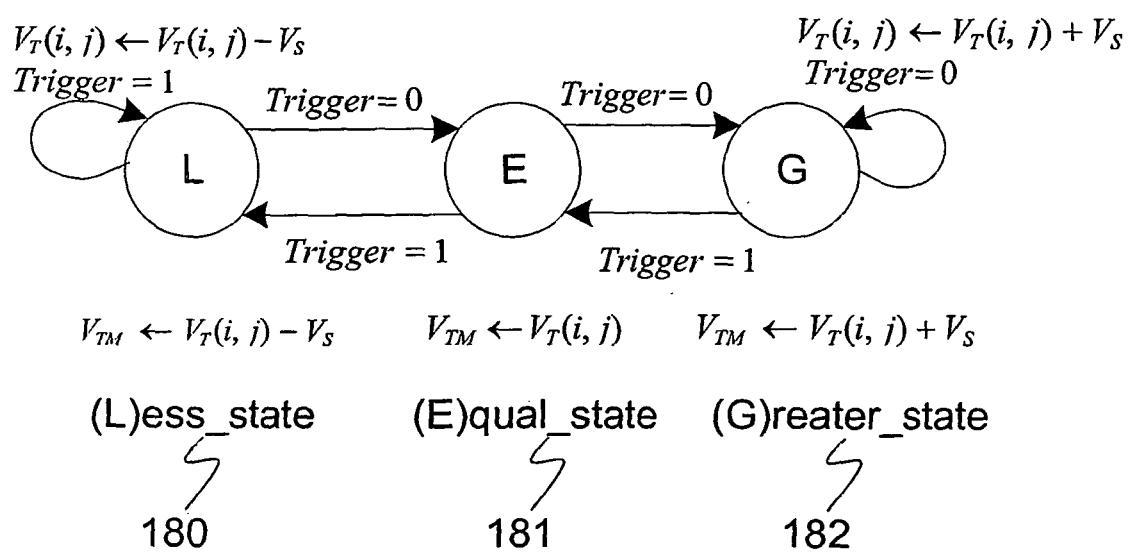


FIG. 10

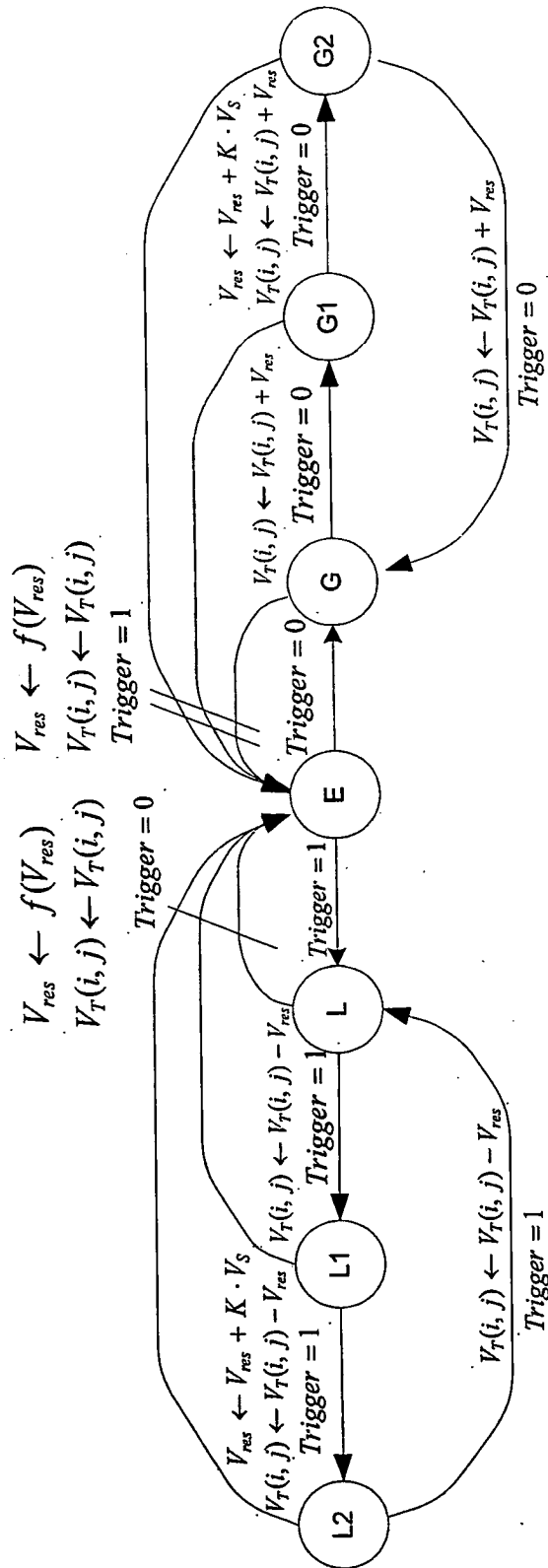


FIG. 11

L2, L1, and L: $V_{TM} \leftarrow V_T(i, j) - V_{res}$ E: $V_{TM} \leftarrow V_T(i, j)$ G2, G1, and G: $V_{TM} \leftarrow V_T(i, j) + V_{res}$

$$f(V_{res}) = \begin{cases} V_S & V_{res} \leq (A-1)V_S \\ \frac{V_{res} - V_S}{A} & V_{res} > (A-1)V_S \end{cases}$$

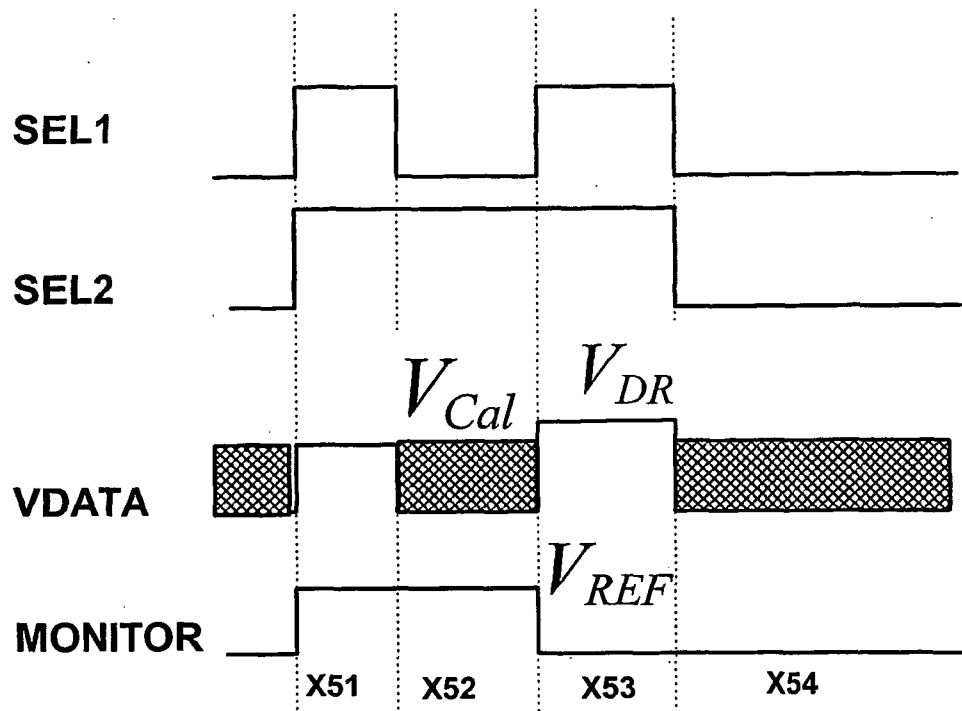


FIG. 12

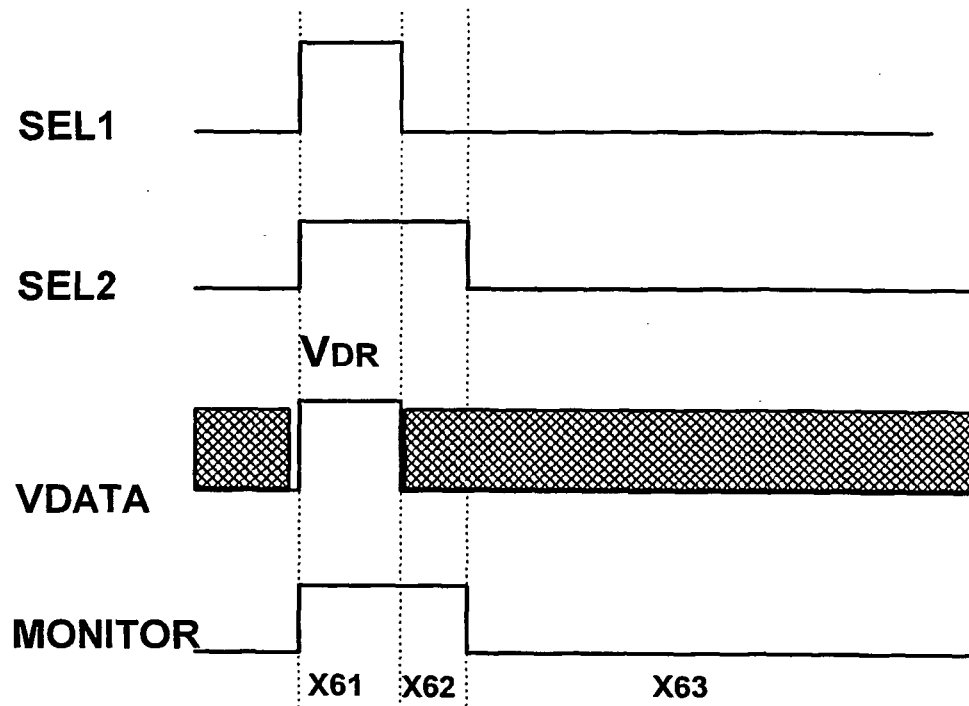


FIG. 13

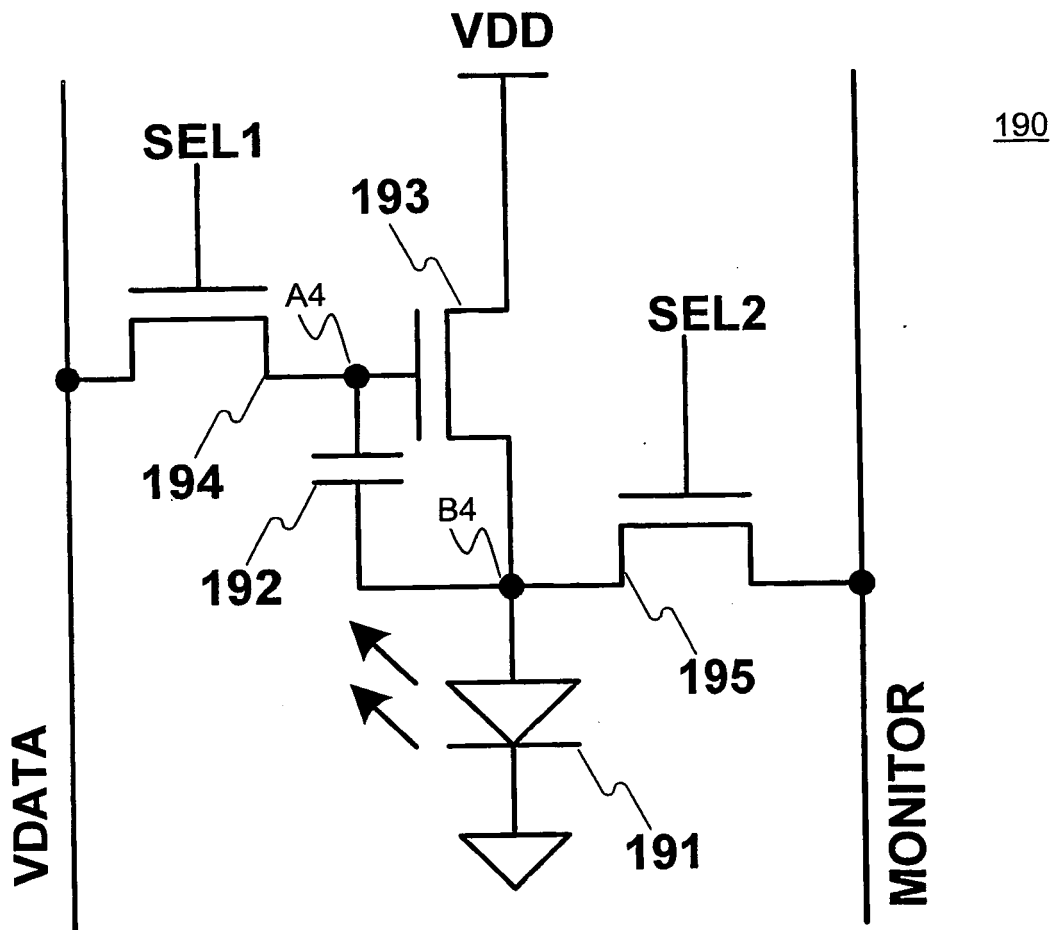
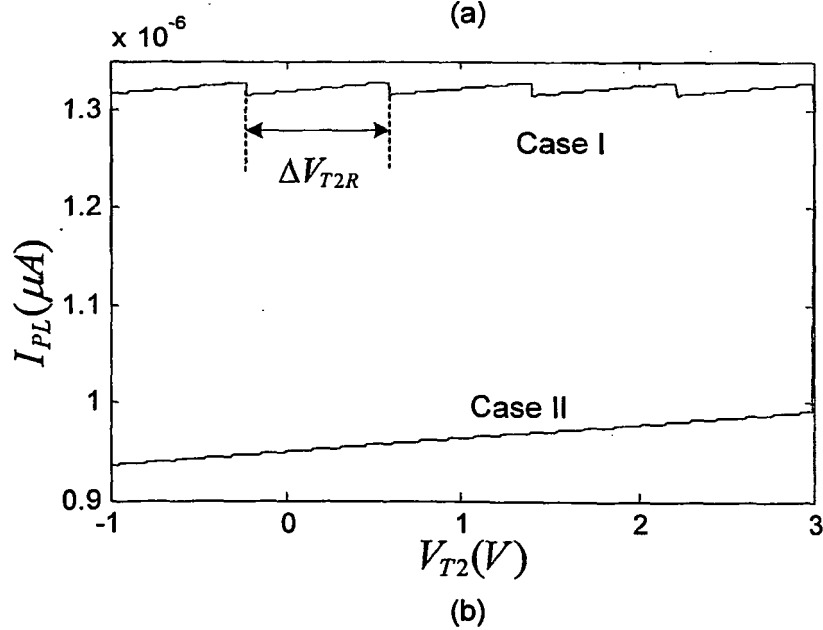
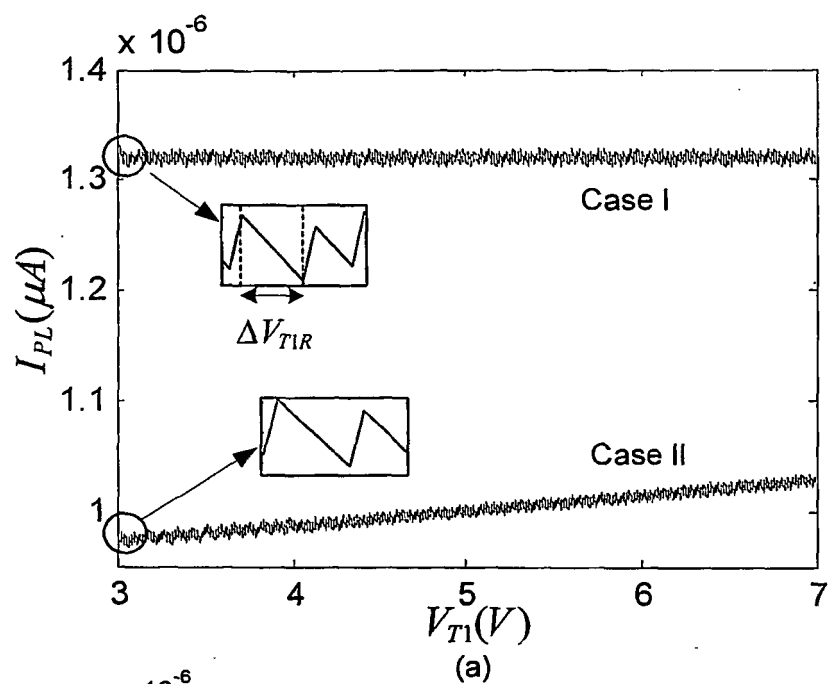
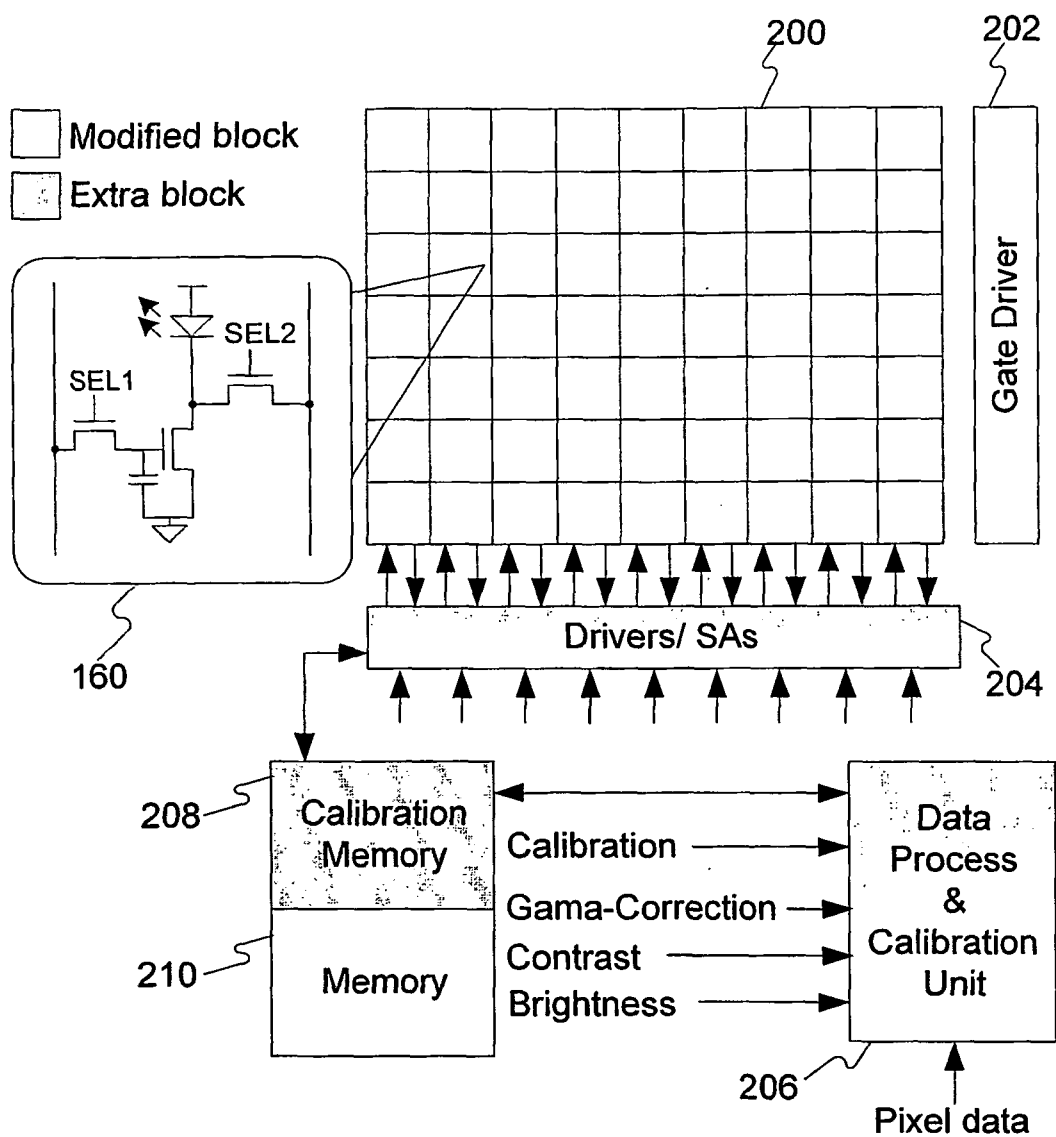


FIG. 14

**FIG. 15**

**FIG. 16**

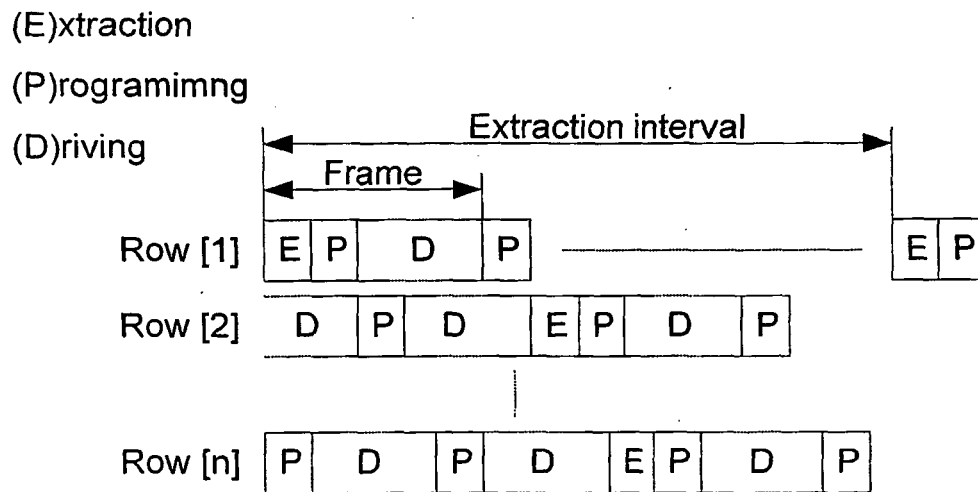


FIG. 17

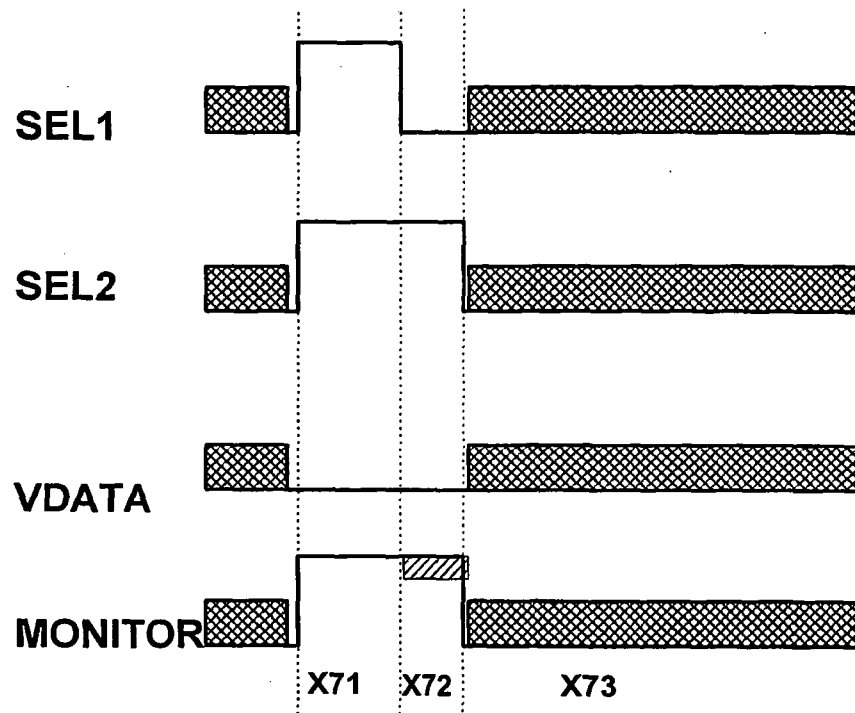


FIG. 18

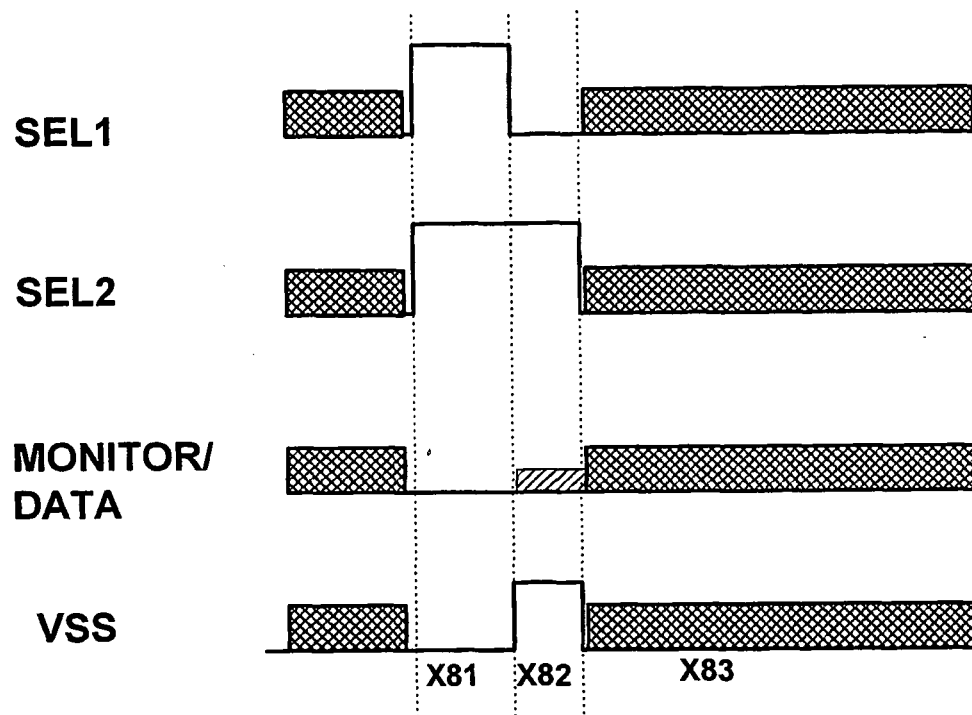


FIG. 19

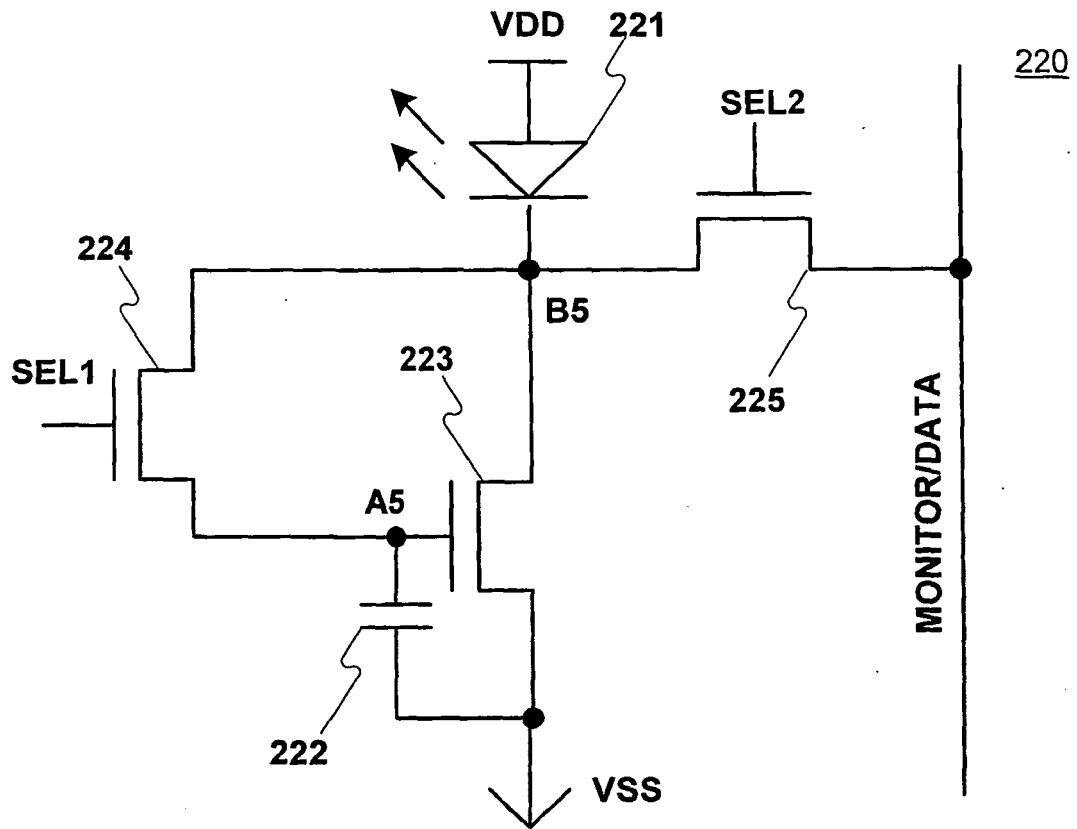


FIG. 20

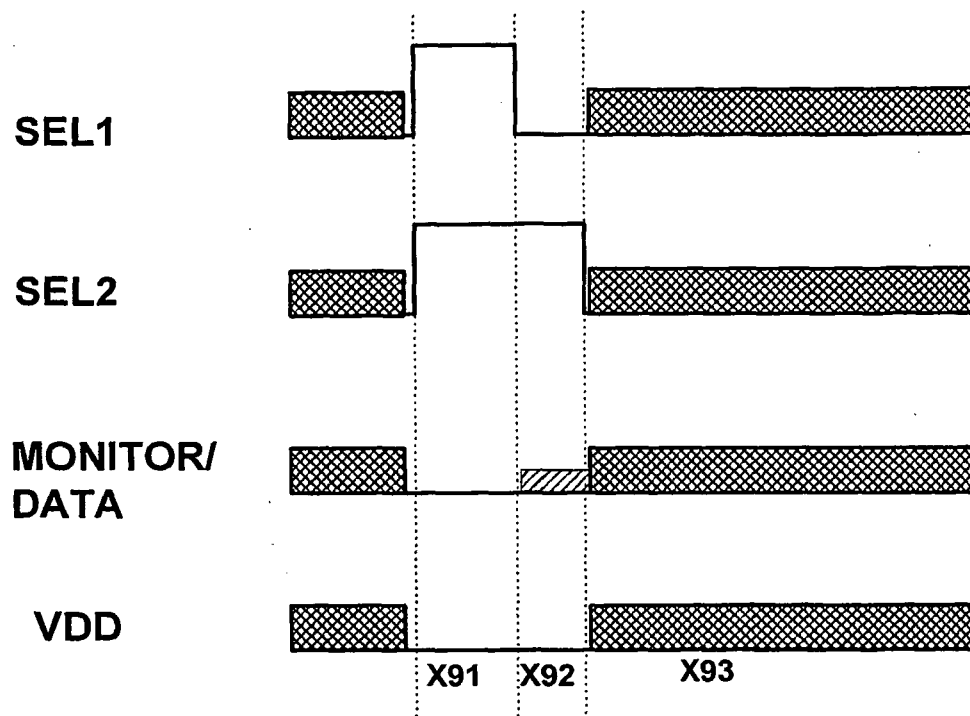


FIG. 21

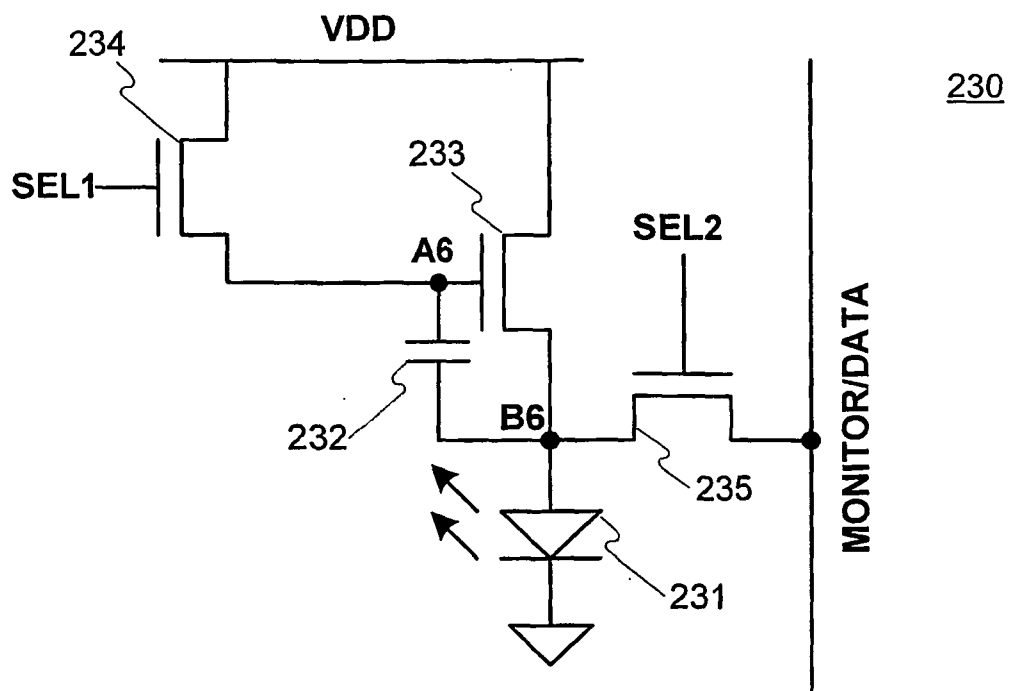


FIG. 22

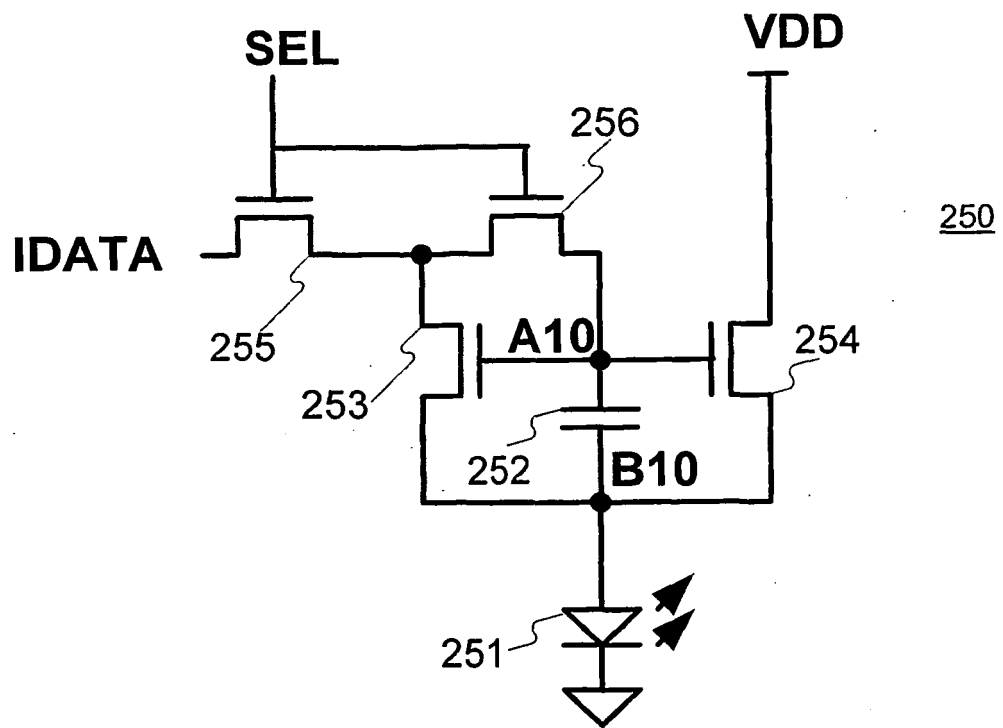


FIG. 23

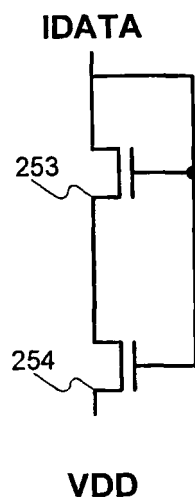


FIG. 24

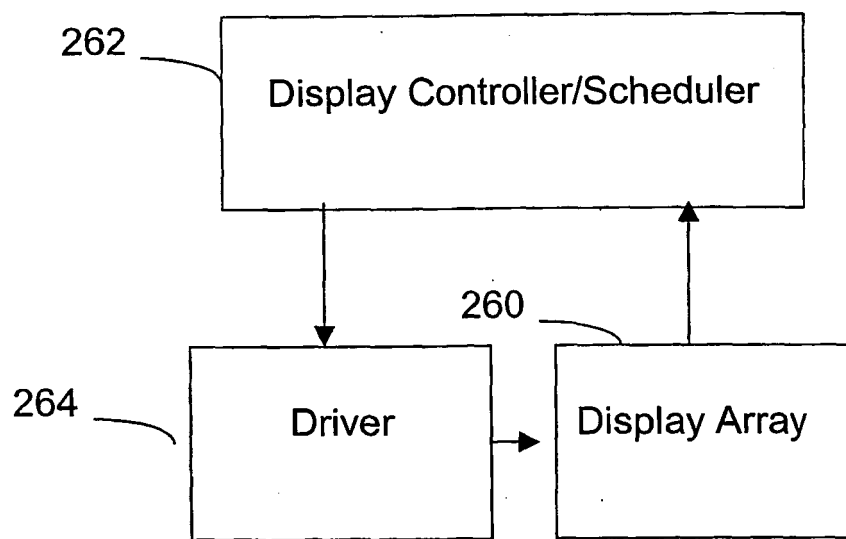


FIG. 25

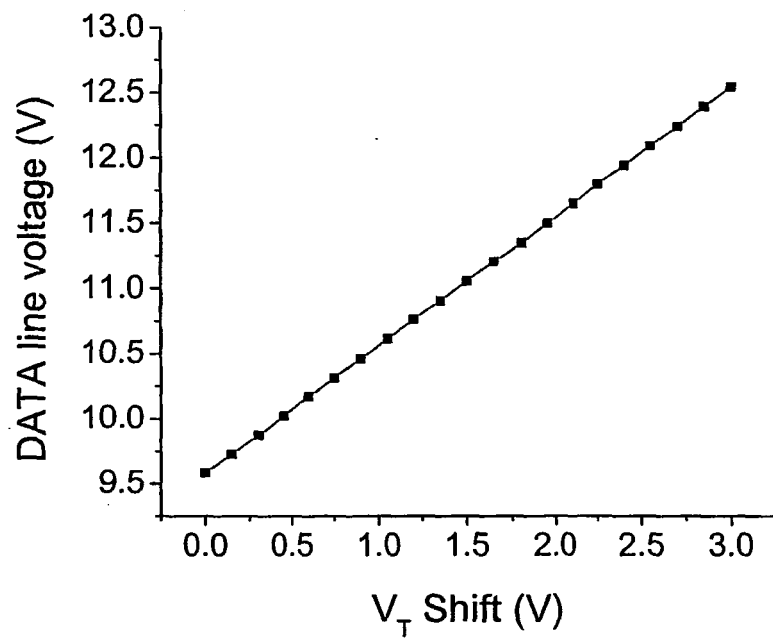


FIG. 26

REFERENCES CITED IN THE DESCRIPTION

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Patent documents cited in the description

- US 6594606 A [0004]
- WO 2005022498 A [0004]
- US 6738035 B [0004]
- US 6690344 B [0004]

专利名称(译)	用于编程，校准和驱动发光器件显示器的方法和系统		
公开(公告)号	EP1836697B1	公开(公告)日	2013-07-10
申请号	EP2005819617	申请日	2005-12-15
[标]申请(专利权)人(译)	伊格尼斯创新公司		
申请(专利权)人(译)	IGNIS创新INC.		
当前申请(专利权)人(译)	IGNIS创新INC.		
[标]发明人	NATHAN AROKIA CHAJI GHOLAMREZA REZA SERVATI PEYMAN		
发明人	NATHAN, AROKIA CHAJI, GHOLAMREZA REZA SERVATI, PEYMAN		
IPC分类号	G09G3/20 G09G3/32		
CPC分类号	G01R19/0092 G09G3/006 G09G3/3208 G09G3/3233 G09G3/3241 G09G3/3258 G09G3/3283 G09G3/3291 G09G2300/0819 G09G2300/0842 G09G2310/0262 G09G2310/027 G09G2320/0285 G09G2320/029 G09G2320/0295 G09G2320/043 G09G2320/045 G09G2320/0693		
代理机构(译)	GRÜNECKER , KINKELDEY , STOCKMAIR & SCHWANHÄUSSER		
优先权	2503237 2005-04-08 CA 2490860 2004-12-15 CA 2521986 2005-10-17 CA 2509201 2005-06-08 CA		
其他公开文献	EP1836697A1 EP1836697A4		
外部链接	Espacenet		

摘要(译)

一种用于显示器阵列的系统，包括像素电路，所述像素电路包括驱动晶体管，至少一个开关晶体管，存储电容器和发光器件。该系统包括用于监视与像素电路相关联的电流或电压的监视器，用于控制显示阵列的操作的数据处理单元，数据处理单元被配置为基于提取指示像素电路老化的信息。监视的电流或电压以及由数据处理单元控制的驱动器，用于基于提取的老化信息向像素电路提供编程和校准数据。

$$I_{Line} = I_{pixel} = \beta (V_p - V_T)^2 \quad \dots (1)$$